

(19) World Intellectual Property Organization  
International Bureau



(43) International Publication Date  
4 December 2003 (04.12.2003)

PCT

(10) International Publication Number  
**WO 03/100986 A2**

(51) International Patent Classification<sup>7</sup>: **H03M 13/00**

(74) Agent: **BERESKIN & PARR**; 40 King Street West, 40th Floor, Toronto, Ontario M5H 3Y2 (CA).

(21) International Application Number: **PCT/CA03/00737**

(81) Designated States (*national*): AE, AG, AL, AM, AT, AU, AZ, BA, BB, BG, BR, BY, BZ, CA, CH, CN, CO, CR, CU, CZ, DE, DK, DM, DZ, EC, EE, ES, FI, GB, GD, GE, GH, GM, HR, HU, ID, IL, IN, IS, JP, KE, KG, KP, KR, KZ, LC, LK, LR, LS, LT, LU, LV, MA, MD, MG, MK, MN, MW, MX, MZ, NO, NZ, OM, PH, PL, PT, RO, RU, SC, SD, SE, SG, SK, SL, TJ, TM, TN, TR, TT, TZ, UA, UG, US, UZ, VC, VN, YU, ZA, ZM, ZW.

(22) International Filing Date: **23 May 2003 (23.05.2003)**

(25) Filing Language: **English**

(26) Publication Language: **English**

(30) Priority Data:  
60/382,581 24 May 2002 (24.05.2002) US  
10/402,215 31 March 2003 (31.03.2003) US

(84) Designated States (*regional*): ARIPO patent (GH, GM, KE, LS, MW, MZ, SD, SL, SZ, TZ, UG, ZM, ZW), Eurasian patent (AM, AZ, BY, KG, KZ, MD, RU, TJ, TM), European patent (AT, BE, BG, CH, CY, CZ, DE, DK, EE, ES, FI, FR, GB, GR, HU, IE, IT, LU, MC, NL, PT, RO, SE, SI, SK, TR), OAPI patent (BF, BJ, CF, CG, CI, CM, GA, GN, GQ, GW, ML, MR, NE, SN, TD, TG).

(71) Applicant (*for all designated States except US*): **AVENDO WIRELESS INC.** [CA/CA]; 2595 Skymark Avenue, Unit 209, Mississauga, Ontario L4W 4L5 (CA).

(72) Inventors; and

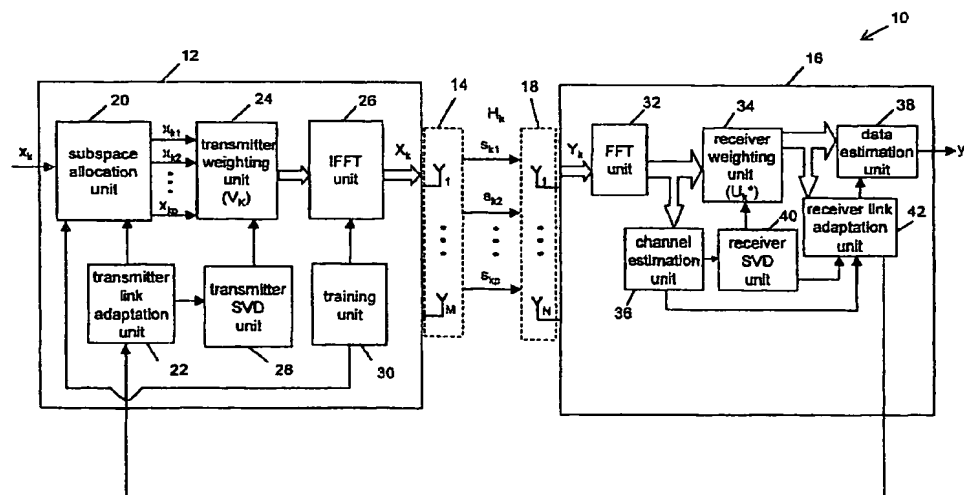
(75) Inventors/Applicants (*for US only*): **OPREA, Alexandru, M.** [CA/CA]; 25 Farmcote Road, North York, Ontario M3B 2Z6 (CA). **ZAMIRI-JAFARIAN, Hossein** [IR/CA]; 25 Saint Mary Street, Apt. 308, Toronto, Ontario M4Y 1R2 (CA).

Published:

— without international search report and to be republished upon receipt of that report

For two-letter codes and other abbreviations, refer to the "Guidance Notes on Codes and Abbreviations" appearing at the beginning of each regular issue of the PCT Gazette.

(54) Title: **SYSTEM AND METHOD FOR DATA DETECTION IN WIRELESS COMMUNICATION SYSTEMS**



(57) Abstract: A system and method for data detection in a wireless communication system wherein the system comprises a receiver for receiving spatial-subspace data transmitted over a plurality of spatial-subspace channels of a sub-carrier which may comprise at least one of coded and uncoded spatial-subspace channels. The receiver comprises a receiver weighting unit for providing receive-weighted spatial-subspace data and a data estimation unit for performing an iterative processing method on the receive-weighted spatial-subspace data to estimate output data related to the input data symbol stream. The iterative processing method comprises successively processing data on each of the plurality of spatial-subspace channels in the receive-weighted spatial-subspace data.

**Title: SYSTEM AND METHOD FOR DATA DETECTION IN WIRELESS  
COMMUNICATION SYSTEMS**

**Reference to Related Application**

**[0001]** This application claims priority from U.S. Provisional Patent Application Serial No. 60/382,581 filed May 24, 2002.

**Field of the invention**

- 5 **[0002]** The invention relates to a system and method for wireless communication and more particularly, this invention relates to a system and method for adaptive channel separation in a wireless communication system.

**Background of the invention**

- 10 **[0003]** Modern wireless communication systems are designed to provide reliable communication at the highest possible bit rate for a given environment. However, there is still a pressing and persistent need for increasingly higher data speed and bandwidth. The available bit rate for an application depends on a number of different parameters such as: available bandwidth, total radiated power at the transmitter, characteristics of the propagation environment, and cost of implementation as well as other factors.

- 15 **[0004]** There are several approaches for increasing the bit rate given the above constraints. One of these approaches involves the use of Multiple Input Multiple Output (MIMO) systems which comprise multiple antennas at both the transmitter and the receiver. A MIMO system provides an opportunity  
20 to exploit spatial channel diversity thereby increasing the spectral efficiency and error performance of a wireless communication system. Space-time coding may also be used to distinguish the signals that are sent by the various transmitter antennas as well as to increase the robustness of the MIMO system to errors caused by noise and the multi-path phenomenon.

- 25 **[0005]** Another approach for increasing bit rate is to simultaneously transmit information on a plurality of independent frequencies that are orthogonal to one another. This technique is known as Orthogonal Frequency Division Multiplexing (OFDM) in which there are a plurality of sub-carriers that are narrowband and orthogonal to each other. Each sub-carrier carries a data

- 2 -

symbol and the sub-carriers are transmitted simultaneously in large numbers to achieve a high overall data rate. OFDM is an effective transmission modulation scheme for combating the adverse effects of noise sources and in particular multipath fading. OFDM is typically implemented using the Fast  
5 Fourier Transform (FFT) which is a well-known process for transforming a non-orthogonal signal into a plurality of orthogonal components (i.e. sub-carriers).

[0006] Another approach for increasing the throughput of the MIMO system is to decompose the multiple channels into several independent  
10 channels through the use of Singular Value Decomposition (SVD). The SVD of the channel matrix (which defines the interaction of each transmitter antenna with each receiver antenna) can be used to decompose a MIMO system having M transmitter antennas (i.e. M inputs) and N receiver antennas (i.e. N outputs) into p-one dimensional channels (where  $p < M$  and  $p < N$ ). The  
15 channel matrix (i.e. the matrix H) has M rows and N columns and is estimated at the initial-setup of the MIMO system by using training symbols as is well known to those skilled in the art. The SVD of the channel matrix H is calculated to obtain a triplet of matrices (U,  $\Lambda$  and  $V^*$ ) where \* represents the complex conjugate transpose. The matrix  $\Lambda$  is the singular value matrix which  
20 represents the independent channels. The matrix V is used to weight the data that is transmitted by the transmitter antennas and the matrix  $U^*$  is used to weight the data that is received by the receiver antennas. Accordingly, either the channel matrix H or the matrix V must be sent to the transmitter. Furthermore, the channel matrix H is updated on a periodic or intermittent  
25 basis during regular data transmission since the channel will vary during the operation of the MIMO system (i.e. the channel is considered to be quasi-static). Accordingly, the U,  $\Lambda$  and  $V^*$  matrices vary during the operation of the MIMO system.

[0007] Another approach for increasing throughput is a MIMO system  
30 which combines OFDM and SVD. In this case, the MIMO system comprises a plurality of sub-carriers which each have an associated channel matrix ( $H_k$  for

- 3 -

a sub-carrier  $k$ ). The SVD is calculated for each of the channel matrices  $H_k$  and the channel matrix  $H_k$  or the  $V_k$  matrix is transmitted to the transmitter for each of the sub-carriers. For exemplary purposes, given a MIMO system with 8 transmitter antennas and 8 receiver antennas, the channel matrix  $H_k$  is an 8x8 matrix. Assuming 16 bits are used to encode a real number and 16 bits are used to calculate an imaginary number, an 8x8 channel matrix  $H_k$  (which in general contains complex numbers) requires  $8 \times 8 \times (16+16) = 2048$  bits of data. With an OFDM system which uses 768 carriers, there will be 768 channel matrices which requires  $768 \times 2048 = 1.5$  Mbits of data. Further, assuming that each channel matrix  $H_k$  is updated every millisecond, then the data rate required simply for sending each channel matrix  $H_k$  to the transmitter is 1 GHz which is excessive.

**[0008]** As discussed, instead of sending the channel matrices  $H_k$  to the transmitter, the  $V_k$  weight matrices may be sent. The row size of each  $V_k$  matrix is equal to the number of receiver antennas and the column size of each  $V_k$  matrix is equal to the number of useable subspaces that result from the singular value decomposition of the corresponding channel matrix  $H_k$ . Assuming that there are four useable subspaces, 16 bits are used to encode a real number and 16 bits are used to encode an imaginary number, an 8x4  $V_k$  matrix (which contains complex numbers) requires  $8 \times 4 \times (16+16) = 1024$  bits of data. Once again, assuming an OFDM system which uses 768 carriers, there will be 768  $V_k$  matrices which requires  $768 \times 1024 = 0.78$  Mbits of data. This translates to a data rate of 0.8 GHz assuming that each  $V_k$  matrix is updated every millisecond.

**[0009]** Accordingly, a MIMO system which incorporates both OFDM and SVD requires a large data rate for providing channel information to the transmitter. This issue is more pronounced if frequency division duplexing is also used. In addition, the SVD operation is an iterative algorithm which is computationally intensive and must be performed for each channel matrix  $H_k$ , every millisecond. Both of these operations in their present form are

- 4 -

computationally intensive and are not suitable for an efficient SVD-based MIMO system.

**Summary of the invention**

**[0010]** In a first aspect, the present invention provides a communication  
5 system for transmitting an input data symbol stream over a plurality of spatial-  
subspace channels of a sub-carrier between a transmitter and a receiver. The  
transmitter comprises an encoder unit for processing a plurality of input data  
symbol sub-streams for providing a plurality of uncoded/coded input data  
symbol sub-streams comprising at least one of: 1) at least one uncoded input  
10 data symbol sub-stream for allocation on a corresponding at least one  
uncoded spatial-subspace channel of the plurality of spatial-subspace  
channels and 2) at least two coded input data symbol sub-streams for  
allocation on a corresponding at least two coded spatial-subspace channels of  
the plurality of spatial-subspace channels. The plurality of input data symbol  
15 sub-streams are derived from the input data symbol stream. The transmitter  
further comprises a transmitter weighting unit connected to the encoder unit  
for weighting the plurality of uncoded/coded input data symbol sub-streams  
with a transmit weight matrix corresponding to the sub-carrier for distributing  
the plurality of uncoded/coded input data symbol sub-streams along the  
20 plurality of spatial-subspace channels and providing transmit-weighted spatial-  
subspace data. The receiver comprises a receiver weighting unit for receiving  
spatial-subspace data related to the transmit-weighted spatial-subspace data  
and weighting the spatial-subspace data with a receive weight matrix for  
providing receive-weighted spatial-subspace data. The receiver also  
25 comprises a data estimation unit connected to the receiver weighting unit for  
receiving and performing an iterative processing method on the receive-  
weighted spatial-subspace data to estimate output data related to the input  
data symbol stream, the iterative processing method comprising successively  
processing data on each of the plurality of spatial-subspace channels in the  
30 receive-weighted spatial-subspace data.

- 5 -

**[0011]** In a second aspect, the present invention provides a method for transmitting an input data symbol stream over a plurality of spatial-subspace channels of a sub-carrier between a transmitter and a receiver. At the transmitter the method comprises:

- 5 a) processing a plurality of input data symbol sub-streams for providing a plurality of uncoded/coded input data symbol sub-streams comprising at least one of: 1) at least one uncoded input data symbol sub-stream for allocation on a corresponding at least one uncoded spatial-subspace channel of the plurality of
- 10 spatial-subspace channels and 2) at least two coded input data symbol sub-streams for allocation on a corresponding at least two coded spatial-subspace channels of the plurality of spatial-subspace channels, the plurality of input data symbol sub-streams being derived from the input data symbol stream; and,
- 15 b) weighting the plurality of uncoded/coded input data symbol sub-streams with a transmit weight matrix corresponding to the sub-carrier for distributing the plurality of uncoded/coded input data symbol sub-streams along the plurality of spatial-subspace channels and providing transmit-weighted spatial-subspace
- 20 data;

At the receiver the method further comprises:

- c) receiving spatial-subspace data related to the transmit-weighted spatial-subspace data and weighting the spatial-subspace data with a receive weight matrix for providing
- 25 receive-weighted spatial-subspace data; and,
- d) performing an iterative processing method on the receive-weighted spatial-subspace data to estimate output data related to the input data symbol stream, the iterative processing method comprising successively processing data on each of the plurality

- 6 -

of spatial-subspace channels in the receive-weighted spatial-subspace data.

**[0012]** In another aspect, the present invention provides a receiver for receiving spatial-subspace data transmitted over a plurality of spatial-subspace channels of a sub-carrier. The spatial-subspace data comprises a plurality of uncoded/coded data symbol sub-streams comprising at least one of: 1) at least one uncoded input data symbol sub-stream for allocation on a corresponding at least one uncoded spatial-subspace channel of the plurality of spatial-subspace channels and 2) at least two coded input data symbol sub-streams for allocation on a corresponding at least two coded spatial-subspace channels of the plurality of spatial-subspace channels. The receiver comprises a receiver weighting unit for weighting the spatial-subspace data with a receive weight matrix for providing receive-weighted spatial-subspace data; and, a data estimation unit connected to the receiver weighting unit for receiving and performing an iterative processing method on the receive-weighted spatial-subspace data to estimate output data related to the input data symbol stream. The iterative processing method comprises successively processing data on each of the plurality of spatial-subspace channels in the receive-weighted spatial-subspace data.

**[0013]** In yet another aspect, the present invention provides a method for receiving spatial-subspace data transmitted over a plurality of spatial-subspace channels of a sub-carrier. The spatial-subspace data comprises a plurality of uncoded/coded data symbol sub-streams comprising at least one of: 1) at least one uncoded input data symbol sub-stream for allocation on a corresponding at least one uncoded spatial-subspace channel of the plurality of spatial-subspace channels and 2) at least two coded input data symbol sub-streams for allocation on a corresponding at least two coded spatial-subspace channels of the plurality of spatial-subspace channels. The method comprises:

- 7 -

a) weighting the spatial-subspace data with a receive weight matrix for providing receive-weighted spatial-subspace data; and,

5 b) performing an iterative processing method on the receive-weighted spatial-subspace data to estimate output data related to the input data symbol stream, the iterative processing method comprising successively processing data on each of the plurality of spatial-subspace channels in the receive-weighted spatial-subspace data.

10 **[0014]** In yet another aspect, the present invention provides a communication system for transmitting input data over a plurality of spatial-subspace channels of a sub-carrier between a transmitter and a receiver. The transmitter comprises an encoder unit for processing a plurality of input data symbol sub-streams for providing a plurality of uncoded/coded input data  
15 symbol sub-streams comprising at least one of: 1) at least one uncoded input data symbol sub-stream for allocation on a corresponding at least one uncoded spatial-subspace channel of the plurality of spatial-subspace channels and 2) at least two coded input data symbol sub-streams for allocation on a corresponding at least two coded spatial-subspace channels of  
20 the plurality of spatial-subspace channels. The transmitter transmits data related to the plurality of uncoded/coded input data symbol sub-streams. The receiver comprises a data estimation unit for performing an iterative processing method on received spatial-subspace data to estimate output data related to the input data. The iterative processing method comprises  
25 successively processing data on each of the plurality of spatial-subspace channels in the received spatial-subspace data.

**[0015]** In another aspect, the present invention provides a method for transmitting input data over a plurality of spatial-subspace channels of a sub-carrier between a transmitter and a receiver. At the transmitter the method  
30 comprises: a) processing a plurality of input data symbol sub-streams for providing a plurality of uncoded/coded input data symbol sub-streams



- 8 -

comprising at least one of: 1) at least one uncoded input data symbol sub-stream for allocation on a corresponding at least one uncoded spatial-subspace channel of the plurality of spatial-subspace channels and 2) at least two coded input data symbol sub-streams for allocation on a corresponding at least two coded spatial-subspace channels of the plurality of spatial-subspace channels, and transmitting data related to the plurality of uncoded/coded input data symbol sub-streams. At the receiver the method further comprises: b) performing an iterative processing method on received spatial-subspace data to estimate output data related to the input data, the iterative processing method comprising successively processing data on each of the plurality of spatial-subspace channels in the received spatial-subspace data.

**Brief description of the drawings**

[0016] For a better understanding of the present invention and to show more clearly how it may be carried into effect, reference will now be made, by way of example only, to the accompanying drawings which show a preferred embodiment of the present invention and in which:

[0017] Figure 1 is a block diagram of an SVD-based OFDM-MIMO communication system in accordance with the present invention;

[0018] Figure 2 is a flow diagram of a partial SVD algorithm used by the SVD-based OFDM-MIMO communication system of Figure 1;

[0019] Figure 3a is a diagrammatic representation of the channel information in the frequency domain for the OFDM-MIMO system of Figure 1;

[0020] Figure 3b is a diagrammatic representation of the channel information in the time domain for the OFDM-MIMO system of Figure 1;

[0021] Figure 3c is a diagrammatic representation of the relation between the channel information in the time and frequency domains;

[0022] Figure 3d is a graph of a typical impulse response for the OFDM-MIMO system of Figure 1;

- [0023] Figure 4 is a flow diagram of a process for creating channel-related data used by the SVD-based OFDM-MIMO communication system of Figure 1 based on truncated impulse response data;
- 5 [0024] Figure 5a is a block diagram of an alternative SVD-based OFDM-MIMO communication system;
- [0025] Figure 5b is a block diagram of the transmitter of the SVD-based OFDM-MIMO communication system of Figure 5a;
- [0026] Figure 5c is a block diagram of the receiver of the SVD-based OFDM-MIMO communication system of Figure 5a;
- 10 [0027] Figure 6a is a diagram illustrating the general data structure used in the communication system of Figures 5a to 5c comprising OFDM super-frames;
- [0028] Figure 6b is a diagram of the data structure of a channel training block used in an OFDM super-frame for channel estimation;
- 15 [0029] Figure 6c is a diagram of the data structure of a CTI symbol used in an OFDM frame;
- [0030] Figure 6d is a diagram of the distribution of synchronization symbols SY used in the synchronization of OFDM frames;
- [0031] Figure 7a is a diagram of a data structure employing a time-division multiplexing scheme for subspace tracking on the spatial-subspace channel level;
- 20 [0032] Figure 7b is a diagram of the time-division multiplexing scheme for incorporating subspace training symbols  $\Delta T$  for tracking subspace information on the transmitter antenna level;
- 25 [0033] Figure 7c is a diagram of the data structure of OFDM frames incorporating subspace training symbols  $\Delta T$  for tracking subspace information and synchronization symbols SY for synchronization;
- [0034] Figure 8 is a diagram of an example of the overall OFDM data structure used by the communication system of Figures 5a to 5c; and,

- 10 -

[0035] Figure 9 is a block diagram of a data estimation unit used by the receiver of Figure 5c.

**Detailed description of the invention**

[0036] Referring to Figure 1, shown therein is a block diagram of an SVD-based OFDM-MIMO communication system 10 in accordance with the present invention. The communication system 10 comprises a transmitter 12 with a transmitter antenna array 14 having M transmitting antenna elements, and a receiver 16 with a receiver antenna array 18 having N receiving antenna elements. The transmitter 12 and the receiver 16 are connected by a multi-path communications channel. The transmitter 12 processes an input data symbol stream, which generally comprises complex data symbols, by allocating a portion of the input data symbol stream  $x_k$  to different spatial-subspace channels of a given sub-carrier k, and providing a stream of (different) OFDM data symbol waveforms to each antenna element of the transmitter antenna array 14. It should be understood that the term data symbol stream represents a stream of data symbols where each data symbol is related to a group of input data bits (as explained below). A data symbol should not be confused with an OFDM data symbol. An OFDM data symbol is a collection of data symbols across all OFDM sub-carriers.

[0037] The OFDM data symbol waveforms are transmitted to the receiver antenna array 18 of the receiver 16 via a communications channel that comprises a plurality of signal paths for each OFDM sub-carrier k. The signal paths comprise several spatial-subspace channels  $s_{k1}, s_{k2}, \dots, s_{kp}$  (for simplicity, only the spatial-subspace channels for sub-carrier k are shown). The receiver 16 processes the received data symbol waveforms to provide an output data symbol stream  $y_k$  which comprises complex data symbols corresponding to those in the input data symbol stream  $x_k$ . Alternatively, both the transmitter 12 and the receiver 16 may function as transceivers. The communication system 10 will be described in terms of a generic sub-carrier k, however, it should be understood by those skilled in the art that each of the

- 11 -

operations performed by the communication system 10 is repeated for each sub-carrier.

[0038] The input data symbol stream  $x_k$  is generated from an input binary stream by grouping a number of consecutive bits of the input binary stream and applying a mapping process to these consecutive data bits to generate input data symbols. The mapping process can be any appropriate modulation scheme such as Quadrature Amplitude Modulation (QAM). The input binary stream may be provided by any number of devices such as a computer, a router or an electronic communication device. Similarly, the output data symbol stream  $y_k$  is applied to a corresponding de-mapping process to obtain an output binary stream that corresponds to the input binary stream. The output binary stream may be provided to a computer, router or other electronic communication device. It should be understood by those skilled in the art that appropriate hardware (not shown) is connected to the transmitter antenna array 14 for providing digital-to-analog conversion and RF up-conversion prior to transmission of the data symbol waveforms. Corresponding hardware (not shown) is connected to the receiver antenna array 18 for providing RF down-conversion and analog-to-digital conversion after reception of the data symbol waveforms.

[0039] The spatial nature of the sub-carriers results from the creation of multiple spatial channels due to the use of multiple antenna elements at the transmitter 12 and the receiver 16. The spatial channels between the transmitter antenna array 14 and the receiver antenna array 18 can be represented by a quasi-static channel matrix  $H_k$  which describes the channel between each antenna element of the transmitter antenna array 14 and each antenna element of the receiver antenna array 18 for a given sub-carrier  $k$ . Given that an input symbol vector of  $M$  elements  $X_k$  is applied at the input of the transmitter antenna array 14 and an output symbol vector of  $N$  elements  $Y_k$  is received at the output of the receiver antenna array 18, then the relation between the input symbol vector  $X_k$ , the output symbol vector  $Y_k$  and the channel matrix  $H_k$  is as shown in equation 1.

- 12 -

$$\mathbf{Y}_k = \mathbf{H}_k \mathbf{X}_k + \mathbf{n}_k \quad (1)$$

The matrix  $\mathbf{H}_k$  is an  $M \times N$  complex-valued channel matrix given by:

$$\mathbf{H}_k = \begin{bmatrix} H_k(1,1) & \cdots & H_k(1,N) \\ \vdots & \ddots & \vdots \\ H_k(M,1) & \cdots & H_k(M,N) \end{bmatrix} \quad (2)$$

and  $\mathbf{n}_k$  is a zero-mean complex Gaussian noise vector.

- 5 **[0040]** The plurality of spatial-subspace channels for a given sub-carrier  $k$  is due to the use of the SVD operation on the corresponding channel matrix  $\mathbf{H}_k$ . Using the SVD operation, the channel matrix  $\mathbf{H}_k$  is decomposed into a product of three matrices  $\mathbf{U}_k$ ,  $\mathbf{\Lambda}_k$ , and  $\mathbf{V}_k^*$  as given by equation 3.

$$\mathbf{H}_k = \mathbf{U}_k \mathbf{\Lambda}_k \mathbf{V}_k^* \quad (3)$$

- 10 where  $\mathbf{\Lambda}_k$  is a diagonal matrix of real, non-negative singular values,  $\lambda_{k,1} > \lambda_{k,2} > \lambda_{k,3} > \dots > \lambda_{k,p} > 0$  with  $p = \text{rank}(\mathbf{H}_k)$ ,  $\mathbf{U}_k$  and  $\mathbf{V}_k^*$  are unitary matrices and  $\mathbf{V}_k^*$  is the complex-conjugate transpose of  $\mathbf{V}_k$ . The dimensions of the matrices are as follows:  $\mathbf{H}_k$  is  $M \times N$ ,  $\mathbf{U}_k$  is  $M \times p$ ,  $\mathbf{\Lambda}_k$  is  $p \times p$ , and  $\mathbf{V}_k^*$  is  $p \times N$ . The magnitude of each singular value relates to the quality of the associated spatial-subspace channel for the OFDM sub-carrier  $k$ .

- 15 **[0041]** Matrix manipulation can be used to determine the diagonal matrix  $\mathbf{\Lambda}_k$  based on the channel matrix  $\mathbf{H}_k$  as given by equation 4.

$$\mathbf{\Lambda}_k = \mathbf{V}_k \mathbf{H}_k \mathbf{U}_k^* \quad (4)$$

- Starting with equation 1 and first pre-multiplying the input symbol vector  $\mathbf{X}_k$  with the transmit weight matrix  $\mathbf{V}_k$  and pre-multiplying the entire right-hand side of equation 1 with the receive weight matrix  $\mathbf{U}_k^*$ , corresponding to the system layout given in Figure 1, the output symbol vector  $\mathbf{Y}_k$  is given by equation 5:

$$\mathbf{Y}_k = \mathbf{U}_k^* (\mathbf{H}_k \mathbf{V}_k \mathbf{X}_k + \mathbf{n}_k) = \mathbf{\Lambda}_k \mathbf{X}_k + \mathbf{U}_k^* \mathbf{n}_k \quad (5)$$

- 25 in which the channel matrix  $\mathbf{H}_k$  has been diagonalized to provide orthogonal spatial-subspace channels for the sub-carrier  $k$ . The channel matrix  $\mathbf{H}_k$  is diagonalized by controlling the weights applied at the transmitter 12 and

- 13 -

receiver 16 in a joint manner (i.e. simultaneously). These weights must be updated on a periodic basis since the channel matrix  $H_k$  is quasi-static.

- [0042] The transmitter 12 further comprises a subspace allocation unit 20, a transmitter link adaptation unit 22, a transmitter weighting unit 24, an IFFT unit 26, a transmitter SVD unit 28 and a training unit 30 connected as shown in Figure 1. The subspace allocation unit 20 receives the input data symbol stream  $x_k$  and divides the input data symbol stream into a plurality of input data symbol sub-streams  $x_{k1}, x_{k2}, \dots, x_{kp}$  for allocation on a plurality of spatial-subspace channels  $s_{k1}, s_{k2}, \dots, s_{kp}$  for the OFDM sub-carrier  $k$ . The transmitter link adaptation unit 22 provides transmission information to the subspace allocation unit 20 which is related to subspace quality information (i.e. the quality of the spatial-subspace channels) for the sub-carrier  $k$ . The transmission information is received from the receiver 16 (discussed in further detail below). The subspace allocation unit 20 uses the transmission information for allocating the input data symbol stream  $x_k$  on the plurality of spatial-subspace channels  $s_{k1}, s_{k2}, \dots, s_{kp}$  since some of the spatial-subspace channels may not be suitable for supporting data transmission (i.e. the singular value associated with a particular spatial-subspace channel may have too low a magnitude). The signal voltage carried by each of these spatial-subspace channels is proportional to the corresponding singular value which provides an indication of whether a spatial-subspace channel is strong or weak. The subspace allocation unit 20 may also apply coding techniques to transmit the input data symbol sub-streams  $x_{k1}, x_{k2}, \dots, x_{kp}$  on a combination of spatial-subspace channels as is described in further detail below.
- [0043] The input data symbol sub-streams  $x_{k1}, x_{k2}, \dots, x_{kp}$  are then supplied to the transmitter weighting unit 24 which multiplies the input data symbol sub-streams with complex weighting values provided by the transmit weight matrix  $V_k$  for producing transmit-weighted spatial-subspace data. The transmit-weighted spatial-subspace data corresponds to distributing the input data symbol sub-streams over the spatial-subspace channels  $s_{k1}, s_{k2}, \dots, s_{kp}$  for sub-carrier  $k$ . The spatial-subspace channels  $s_{k1}, s_{k2}, \dots, s_{kp}$  may be

- 14 -

orthogonal to each other. Ideally orthogonal spatial-subspace channels will not interfere in the spatial domain. Alternatively, the spatial-subspace channels  $s_{k1}, s_{k2}, \dots, s_{kp}$  may be dependent on one another (via coding) or there may be a combination of orthogonal and dependent spatial-subspace channels for a given sub-carrier  $k$  (as discussed further below). In this example, there are  $p$  spatial-subspace channels for sub-carrier  $k$ . The total number of communication paths for the communication system 10 is the sum of the number of spatial-subspace channels across all sub-carriers. The output of the transmitter weighting unit 24 is a symbol vector  $X_k$  having  $M$  elements, wherein the elements of the symbol vector  $X_k$  are applied to a separate antenna element of the transmitter antenna array 14.

[0044] The transmit-weighted spatial-subspace data is then provided to the IFFT (i.e. Inverse Fast Fourier Transform) unit 26 which is connected to the transmitter antenna array 14. The IFFT unit 26 is a transmitter processing unit that converts the transmit-weighted spatial-subspace data to the time-domain for producing data symbol waveforms for transmission by the transmitter antenna array 14. The IFFT unit 26 operates in a block fashion by collecting a plurality of transmit-weighted spatial-subspace data symbols for each antenna element of the transmitter antenna array 14, and then performing the IFFT operation to generate an OFDM symbol for each antenna element of the transmitter antenna array 14. The IFFT unit 26 is preferably a bank of IFFT operators with the number of IFFT operators being equivalent to the number of transmitting antennas 14. Alternatively, the output of the transmitter weighting unit 24 may be provided to one IFFT operator in a time division manner and the output of the IFFT operator correspondingly provided to one antenna element of the transmitter antenna array 14.

[0045] The transmit weight matrix  $V_k$  is calculated by the transmitter SVD unit 28 which receives the corresponding channel matrix  $H_k$  from the transmitter link adaptation unit 22. Channel related information associated with the channel matrix  $H_k$  (rather than the channel matrix itself) is included in the transmission information which is sent from the receiver 16 to the

- 15 -

transmitter link adaptation unit 22 for the efficient operation of the communication system 10. The channel related information comprises channel impulse response data as will be discussed in further detail below. The transmitter link adaptation unit 22 calculates the channel matrix  $H_k$  from the channel related data.

[0046] The training unit 30 generates training sequences so that the receiver 16 can estimate the channel matrix  $H_k$  and provide the channel related data to the transmitter link adaptation unit 22. The training sequences are provided to the IFFT unit 26 and are preferably training symbols that have a low peak-to-average power. The training symbols are generated in the frequency domain and converted to the time domain by the IFFT unit 26 prior to transmission. Alternatively, the training unit 30 may generate the training signals in the time domain and directly provide these signals to the transmitter antenna array 14. In this case, the training unit 30 would be connected to the transmitter antenna array 14 rather than the IFFT unit 26.

[0047] Training symbols are periodically generated and transmitted to the receiver 16 for periodically estimating the channel matrix  $H_k$  for each sub-carrier  $k$ . Alternatively, depending on the frequency spacing between the sub-carriers, it may be possible that the communication channel for several adjacent sub-carriers can be adequately characterized by a single channel matrix. In this case, a channel matrix  $H_r$  and one set of triplet matrices  $U_r$ ,  $\Lambda_r$  and  $V_r$  can be used to represent a group of adjacent sub-carriers  $k, \dots, k+r$ .

[0048] The training unit 30 is also connected to the subspace allocation unit 20 for providing subspace training sequences to the subspace allocation unit 20. The subspace training sequences are preferably generated in the frequency-domain (i.e. subspace training symbols) and may be similar to the channel training symbols. The subspace training symbols are inserted periodically into the input data symbol sub-streams for tracking changes in the singular values of the singular value matrix  $\Lambda_k$ . For this purpose, the subspace training symbols are inserted in one spatial-subspace channel at a time. Subspace tracking is discussed in further detail below.



- 16 -

[0049] In addition to the receiver antenna array 18, the receiver 16 further comprises an FFT unit 32, a receiver weighting unit 34, a channel estimation unit 36, a data estimation unit 38, a receiver SVD unit 40 and a receiver link adaptation unit 42 connected as shown in Figure 1. The FFT (i.e. Fast Fourier Transform) unit 32 converts the received data symbol waveforms into the frequency domain. The FFT unit 32 is preferably a bank of FFT operators with the number of FFT operators being equivalent to the number of antenna elements in the receiver antenna array 18. Alternatively, the output of the receiver antenna array 18 may be provided in a time division fashion to one FFT operator.

[0050] In general, the received data symbol waveforms comprise transmit-weighted spatial-subspace data symbols, training symbols (channel or subspace) and other data (i.e. synchronization signals) for maintaining the operation of the communication system 10. The FFT unit 32 provides the transmit-weighted spatial-subspace data and the subspace training symbols to the receiver weighting unit 34 while the FFT unit 32 provides the channel training symbols to the channel estimation unit 36.

[0051] The receiver weighting unit 34 weights the transmit-weighted spatial-subspace data with complex weighting values provided by the receive weight matrix  $U_k^*$  in accordance with equation 5 to provide receive-weighted spatial-subspace data. The receiver weighting unit 34 also weights the subspace training symbols in a similar fashion to provide receive-weighted subspace training symbols. The receiver weighting unit 34 provides the receive-weighted spatial-subspace data and the receive-weighted subspace training symbols to the data estimation unit 38 and the receiver link adaptation unit 42 respectively.

[0052] The data estimation unit 38 processes the receive-weighted spatial-subspace data to provide the output data symbol stream  $y_k$  for each sub-carrier  $k$ . The data estimation unit 38 performs an estimation process since the receive-weighted spatial-subspace data is corrupted by noise. The data estimation unit 38 may also possibly perform a decoding process if

- 17 -

coding was used to combine some of the spatial-subspace channels for the sub-carrier  $k$ . Further, the data estimation unit 38 may comprise a de-mapper for providing an output data bit stream rather than the output data symbol stream  $y_k$ .

- 5 [0053] The channel estimation unit 36 processes the channel training symbols, using a technique described below, for estimating each channel matrix  $H_k$ . The channel estimation unit 36 is connected to the receiver SVD unit 40 so that the receiver SVD unit 40 can process each channel matrix  $H_k$  and determine the corresponding matrices  $U_k^*$  and  $\Lambda_k$ . Accordingly, the
- 10 receiver SVD unit 40 is connected to the receiver weighting unit 34 for providing the weighting values for each matrix  $U_k^*$  to the receiver weighting unit 34. The channel estimation unit 36 also generates channel related data for each channel matrix  $H_k$ . The generation of the channel related data is described in more detail below.
- 15 [0054] The channel estimation unit 36 and the receiver SVD unit 40 are also both connected to the receiver link adaptation unit 42 to provide the channel related data and the corresponding singular value matrix  $\Lambda_k$  respectively. The receiver link adaptation unit 42 processes the singular value matrix  $\Lambda_k$  to determine subspace quality information. The receiver link
- 20 adaptation unit 42 then determines transmission parameters based on the subspace quality information for the sub-carrier  $k$ . The subspace quality information is determined from the magnitude of the singular values which are on the diagonal of the singular value matrix  $\Lambda_k$ . In general, a singular value with a larger magnitude indicates a better quality spatial-subspace channel on
- 25 which data can be transmitted. For example, input data symbol sub-streams that are allocated on a strong spatial-subspace channel can be modulated using a higher order modulation scheme in which the data points in the corresponding constellation are spaced closer together, such as 32QAM for example. The receiver link adaptation unit 42 bundles the transmission
- 30 parameters and the channel related data as channel/transmission information (CTI) and sends the information to the transmitter link adaptation unit 22.

- 18 -

[0055] The magnitude of the singular values can change in time, space and frequency. Accordingly, the receiver link adaptation unit 42 continuously adapts the transmission parameters when the channel estimation unit 36 estimates new channel matrices  $H_k$  (which is done periodically) and the receiver SVD unit 40 subsequently re-calculates the matrices  $U_k^*$  and  $\Lambda_k$ . The receiver link adaptation unit 42 also processes the receive-weighted subspace training symbols to track variations in the singular value matrix  $\Lambda_k$  and provide updated singular value matrices before the receiver SVD unit 40 periodically re-calculates the singular value matrix  $\Lambda_k$ .

[0056] The receiver link adaptation unit 42 is connected to the data estimation unit 38 to provide an initial singular value matrix  $\Lambda_k$ , updated singular value matrices and transmission parameters for the spatial-subspace channels for a given sub-carrier  $k$ . The data estimation unit 38 uses these matrices and the transmission parameters for the estimation and detection of the input data symbols) in the receive-weighted spatial-subspace data which has been corrupted by noise and may have coded spatial-subspace channels. The data estimation unit 38 preferably employs a successive-interference cancellation method for detecting the data symbols on the uncoded spatial-subspace channels. This involves detecting the data symbols received along the strongest spatial-subspace channel first, subtracting these data symbols from the receive-weighted spatial-subspace data, then detecting the data symbols received along the next strongest spatial-subspace channel and subtracting these data symbols from the receive-weighted spatial-subspace data and so on. The strength of the spatial-subspace channels is given by the signal-to-noise-plus-interference ratio of each spatial-subspace channel. If coding is used to combine some of the spatial-subspace channels, then a corresponding decoding/detection method is used by the data estimation unit 38 as will be described in more detail below.

[0057] As is commonly known to those skilled in the art, a sequence of algebraic operations for constructing a singular value decomposition that will reach an exact solution for the diagonalization of a matrix in a finite number of

operations does not exist. In practice, commonly used SVD algorithms, such as the Jacobi-based algorithms, perform many iterations, such as at least 20 iterations for a MIMO system with a large number of antenna elements, to arrive at a precise solution for providing a singular value matrix  $\Lambda_k$  in which

5 the off-diagonal components have a value of zero. However, implementing such an iterative SVD algorithm in the transmitter and receiver SVD units 28 and 40 is too computationally intensive since the SVD operation must be periodically executed for a plurality of channel matrices.

[0058] Accordingly, the transmitter and receiver SVD units 28 and 40

10 implement a partial SVD algorithm or process 50 as outlined in Figure 2. The matrices are initialized as follows:  $\Lambda_{kinit} = H_k$ ,  $U_{kinit} = I$  and  $V_{kinit} = I$ , where  $I$  is the identity matrix. The first step 52 of the partial SVD algorithm 50 is to perform  $n1$  iterations of an iterative SVD algorithm, such as the Jacobi algorithm, on a channel matrix  $H_k$  to obtain an interim receive weight matrix

15  $U_k'$ , an interim singular value matrix  $\Lambda_k'$  and an interim transmit weight matrix  $V_k'$ , where the value of  $n1$  is a low integer preferably chosen in the range of 1 to 4. More preferably, the value of  $n1$  is 2 or 3. It should be understood that any iterative technique could be used. At this point, in the matrix  $\Lambda_k'$ , the magnitudes of the dominant singular values (i.e. the diagonal components of

20 the  $\Lambda_k'$  matrix) start to become noticeable (i.e. a first upper group of diagonal components have much larger values than a second lower group of diagonal components) and the off-diagonal components start having small but non-zero values. A thresholding procedure is then applied to the magnitudes of the singular values of the singular value matrix  $\Lambda_k'$  at step 54 to determine the

25 number of spatial-subspace channels  $p_k$  for the channel matrix  $H_k$ . For example, assuming an 8x8 channel matrix  $H_k$ , the number of practically usable spatial-subspace channels may be three or four. Alternatively, in some sub-carriers, rather than thresholding, a pre-specified number may be used for the number of spatial-subspace channels  $p_k$ . This pre-specified number

30 may be determined experimentally by examining a plurality of estimated channel matrices for the communication system for a particular sub-carrier  $k$ .

- 20 -

The pre-specified number of spatial-subspace channels  $p_k$  may also be dictated by the cost and complexity of the communication system 10.

**[0059]** The next step 56 in the partial SVD algorithm 50 is to truncate the interim singular value matrix  $\Lambda_k'$  by retaining the  $p_k \times p_k$  sub-matrix within matrix  $\Lambda_k'$  and replacing the remaining entries in the matrix  $\Lambda_k'$  with zeros (i.e. zero-padding) to produce a truncated singular value matrix  $\Lambda_k''$ . The uppermost leftmost corner of the  $p_k \times p_k$  sub-matrix coincides with the uppermost leftmost corner of the matrix  $\Lambda_k'$ . An error in the singular values results from the partial SVD algorithm 50 due to this truncation. However, this error may be compensated for by periodically tracking the singular values in the matrix  $\Lambda_k$  which results from the algorithm 50 as described further below. Alternatively, if the error is small then the compensation is not needed. This use of truncation allows for faster convergence in obtaining the SVD of the channel matrix  $H_k$ . The interim receive and transmit weight matrices  $U_k'$  and  $V_k'$  are also truncated during this procedure to produce truncated receive and transmit weight matrices  $U_k''$  and  $V_k''$ . The truncated receive weight matrix  $U_k''$  consists of the  $p_k$  leftmost columns of the matrix  $U_k'$  and the truncated transmit weight matrix  $V_k''$  consists of the  $p_k$  rightmost columns of the matrix  $V_k'$ .

**[0060]** The next step 58 in the partial SVD algorithm 50 is to perform  $n_2$  iterations of the SVD algorithm using the truncated matrices  $U_k''$ ,  $\Lambda_k''$  and  $V_k''$  to obtain the matrices  $U_k$ ,  $\Lambda_k$  and  $V_k$ . Again, the value of  $n_2$  is preferably chosen in the range of 1 to 4. More preferably, the value of  $n_2$  is 2 or 3. The inventors have found that the triplet of matrices  $U_k$ ,  $\Lambda_k$  and  $V_k$  which result from the partial SVD algorithm 50 are an approximation and are quite close to the matrices that result from the use of a full iterative SVD algorithm when applied to a Rician (see later) channel matrix.

**[0061]** In an alternative, rather than selecting a constant number for the iterations  $n_1$  and  $n_2$  in steps 52 and 58, the magnitude of the off-diagonal components of the interim singular value matrix  $\Lambda_k'$  and the truncated singular

- 21 -

value matrix  $\Lambda_k''$ , respectively, may be monitored in relation to the magnitude of the components on the diagonal to determine the number of iterations. For instance, a variable number of iterations  $n1$  and  $n2$  may be performed in steps 52 and 58 until the sum of the square of the magnitude of the off-diagonal components are a pre-specified fraction (for example  $1/20^{th}$ ,  $1/50^{th}$  or  $1/100^{th}$ ) of the sum of the square of the magnitude of the diagonal components. However, for computational efficiency, a maximum number of iterations  $n1_{max}$  and  $n2_{max}$  is preferably pre-specified for  $n1$  and  $n2$ . For instance,  $n1_{max}$  and  $n2_{max}$  may be 4, 6 or 10.

- 10 [0062] It may be possible to further process the singular value matrix  $\Lambda_k$  which results from the partial SVD algorithm 50 by applying the partial SVD algorithm 50 to the matrix  $\Lambda_k$  (whereas previously it was applied to the matrix  $H_k$ ). The advantage of this approach is that the partial SVD algorithm is applied to a reduced size matrix (the matrix  $\Lambda_k$  has dimensions  $p_k \times p_k$  whereas
- 15 the matrix  $H_k$  had dimensions of  $M \times N$ ) so that the computational complexity does not increase significantly. Further, a better estimate of the singular values in the singular value matrix  $\Lambda_k$  can be obtained and the off-diagonal elements of the matrix  $\Lambda_k$  will get closer to zero.

- [0063] The effectiveness and the applicability of the partial SVD algorithm 50 for diagonalizing the channel matrix  $H_k$  is possible due to the correlation properties of the channel matrix  $H_k$  in certain propagation environments. The channel matrix  $H_k$ , in environments where there are preferred directions of signal propagation, can be described as Rician in which there is a subset of strong spatial channels within the channel matrix  $H_k$
- 20 which relate to the strong singular values associated with the channel matrix  $H_k$ .

- [0064] As mentioned previously, once the triplet of matrices  $U_k$ ,  $\Lambda_k$  and  $V_k$  are determined for a sub-carrier  $k$ , channel information must be provided to the transmitter 12 in order to diagonalize the channel matrix  $H_k$  to provide the spatial-subspace channels for the OFDM sub-carrier  $k$ . Referring to Figure 3a, shown therein is a representation of a set of channel frequency response
- 30

- 22 -

matrices **60** for the communication system **10** in the frequency domain for sub-carriers  $k = 1$  to  $F_{\max}$ . The frequency response of a spatial channel between one transmitter antenna and one receiver antenna is represented by a frequency vector where each sample in the frequency vector is taken from  
5 the same location in each of the channel matrices  $H_k$ .

[0065] An equivalent representation of the channel information is shown in Figure 3b, which shows a set of channel impulse matrices **62** for the communication system **10** in the time domain for time indices  $g = 1$  to  $T_{\max}$ . The channel impulse response of a spatial channel between one transmitter  
10 antenna and one receiver antenna is represented by a time vector where each sample in the time vector is taken from the same location in each of the channel impulse matrices  $h_g$ ,  $g = 1$  to  $T_{\max}$ . In general, there are  $T_{\max}$  samples in each channel impulse response vector.

[0066] Referring now to Figure 3c, the two sets of channel matrices **60**  
15 and **62** are related to each other by the Inverse Fourier Transform when going from the frequency domain to the time domain (or alternatively the Fourier Transform when going from the time domain to the frequency domain). In practice, an Inverse Fast Fourier Transform (IFFT) is preferably used to convert from the frequency domain to the time domain. As is well known by  
20 those skilled in the art, the IFFT produces a time domain vector of  $Z$  samples when provided with a frequency domain vector of  $Z$  samples. However, the channel information is encoded differently in the frequency and time domains. In particular, the inventors have realized that most of the channel information is encoded in a first portion of the time domain vector.

25 [0067] Referring now to Figure 3d, shown therein is a general channel impulse response **64** that defines the spatial channel from a transmitter antenna element **b** to a receiver antenna element **c**. As can be seen, the channel impulse response **64** contains a majority of the signal energy (and thus the channel information) in the first  $t_i$  samples, with the remainder of the  
30 samples in the channel impulse response **64** representing mainly noise. Accordingly, only a portion of the channel impulse response **64** is relevant.

Consequently, an improvement in transmission efficiency of the channel information data for the communication system 10 can be obtained by truncating each channel impulse response  $h_g$  and transmitting each truncated channel impulse response to the transmitter 12 rather than sending each channel matrix  $H_k$  or each transmit weight matrix  $V_k$  to the transmitter 12. The value of  $t_i$  may be determined by using an amplitude threshold value on each channel impulse response  $h_g$  such that after the time sample  $t_i$ , the amplitudes of the channel impulse response  $h_g$  are lower than the amplitude threshold value. Another method to determine the value of  $t_i$  is to define a percentage energy threshold value and determine the value of  $t_i$  such that the truncated channel impulse response contains a percentage energy of the total energy of the channel impulse response equivalent to the percentage energy threshold (i.e. for example 90% of the total energy). Accordingly, with both of these methods, there may be a different number of samples in each of the truncated channel impulse responses. Alternatively, the value of  $t_i$  may be pre-specified and used to truncate each channel impulse response  $h_g$  (for example the value of  $t_i$  may be chosen to be the length of the OFDM guard interval). The pre-specified value of  $t_i$  may be determined through experimental trials and chosen such that accurate channel information is contained in each truncated channel impulse response. The inventors have found that a preferable value for  $t_i$  is 64 samples (whereas the original length of the channel impulse response vector is 1024 samples).

[0068] As discussed previously, for an exemplary MIMO system with 8 transmitter antenna elements, 8 receiver antenna elements and 768 sub-carriers, assuming 32 bits of data are used for representing a complex number, sending all of the channel matrices  $H_k$  to the transmitter 12 requires 1.5 Mbits of data. Alternatively, sending all of the transmit weight matrices  $V_k$  to the transmitter 12 requires 0.78 Mbits of data. However, when sending all of the truncated channel impulse responses to the transmitter 12, and assuming that each truncated channel impulse response is truncated to 64 samples, the amount of data required is  $8 \times 8 \times 64 \times 32 = 0.13$  Mbits of data. This represents a substantial savings in the amount of transmitted data by a factor



- 24 -

of 11 when compared to sending the channel matrices  $H_k$  and 6 when compared to sending the transmit weight matrices  $V_k$ .

[0069] Referring now to Figure 4, shown therein is a process 70 for sending channel related data to the transmitter 12 so that the transmit weight matrices  $V_k$  can be calculated at the transmitter 12 for diagonalizing the communication channel of the communication system 10. The process 70 is repeated for each combination of antenna elements from the transmitter antenna array 14 and the receiver antenna array 18. The process 70 begins at step 72 in which the channel impulse response  $h_{b,c}$  for transmitter antenna **b** and receiver antenna **c** is obtained. This may be done in two fashions. Firstly, a pulse may be sent from the  $b^{th}$  transmitter antenna element to the  $c^{th}$  receiver antenna element to obtain the channel impulse response  $h_{b,c}$ . This approach may further include sending several pulses and averaging the resulting channel impulse responses (in the time domain) to reduce noise. Another approach is to send a sequence with good correlation properties and cross-correlate this sequence received at the receiver 16 with a replica of the original sequence at the receiver 16 to obtain an estimate of the channel impulse response. This approach may also include sending several sequences and averaging the resulting channel impulse response estimate to reduce noise. Alternatively, the channel matrices  $H_k$  for the system 10 may be obtained using frequency domain techniques by using channel training symbols, as explained further below, to obtain the three dimensional frequency response channel matrix 60. The IFFT is then done on a frequency response vector taken from the  $b^{th}$  row and the  $c^{th}$  column of the three dimensional frequency channel matrix 60 to obtain the channel impulse response  $h_{b,c}$ .

[0070] The next step 74 is to truncate the channel impulse response  $h_{b,c}$  to produce a truncated channel impulse response  $h'_{b,c}$  which retains only the first  $t_i$  samples of the channel impulse response  $h_{b,c}$ . As mentioned previously, this truncation provides the benefit of reducing the amount of data that has to be transmitted to the transmitter 12. However, this truncation also

- 25 -

provides the benefit of noise reduction since there is mostly noise and not much signal after the first  $t_i$  samples in the channel impulse response  $h_{b,c}$ . The next step 76 is to send the truncated channel impulse response  $h'_{b,c}$  to the transmitter 12.

5 [0071] Once the transmitter 12 receives the truncated channel impulse response  $h'_{b,c}$ , the next step 78 is to zero pad the truncated channel impulse response  $h'_{b,c}$  thereby producing a zero-padded channel impulse response  $h^0_{b,c}$ . The truncated channel impulse response  $h'_{b,c}$  is preferably zero-padded to the original length of the channel impulse response  $h_{b,c}$ . The next step 80 is to perform the FFT on the zero-padded channel impulse response  $h^0_{b,c}$ . This provides a frequency response vector  $H_f(b,c)$  which spans the sub-carriers of the system 10 and corresponds to a row vector along frequency for transmitter antenna element  $b$  and receiver antenna element  $a$  in the three dimensional frequency response channel matrix 60.

15 [0072] The step 80 of performing the FFT on the zero-padded channel impulse response  $h^0_{b,c}$  provides the advantage of spreading out the noise in the truncated channel impulse response  $h'_{b,c}$  along a larger number of samples (i.e. from the  $t_i$  samples in the truncated channel impulse response  $h'_{b,c}$  to the total number of samples in the zero-padded channel impulse response  $h^0_{b,c}$ ). For example, assuming there is 1024 samples in the zero-padded channel impulse response  $h^0_{b,c}$  and 64 samples in the truncated channel impulse response  $h'_{b,c}$ , an improvement of 1024/64 (i.e. 12 dB) in signal to noise ratio is obtained in step 80. The channel estimation unit 36 performs steps 72 to 74 of process 70 and the transmitter link adaptation unit 25 22 performs steps 78 to 80 of process 70.

[0073] The process 70 is performed for the impulse response of each combination of the antenna elements of the transmitter antenna array 14 and the receiver antenna array 18 in order to produce a plurality of frequency response vectors for constructing the three-dimensional frequency response channel matrix 60 at the transmitter 12. The individual channel matrices  $H_k$  for each sub-carrier  $k$  can then be obtained from the three-dimensional frequency

- 26 -

response channel matrix **60** by taking a vertical slice at frequency index  $k$ . The SVD can then be performed by the transmitter SVD unit **28** on each of the channel matrices  $H_k$  to obtain the corresponding transmit weight matrices  $V_k$ .

5 **[0074]** Furthermore, since the communication system **10** may be a frequency duplex system in which a communication channel exists for a first set of sub-carriers from the transmitter **12** to the receiver **16** and for a second set of sub-carriers from the receiver **16** to the transmitter **12**, the process **70** may be performed to send channel related data to either the transmitter **12** or  
10 the receiver **16**. In this case, the communications system can be considered to have a first processing unit and a second processing unit with a communications channel therebetween. The first processing unit sends channel training signals to the second processing unit which estimates channel impulse response data, truncates this data and sends the truncated  
15 channel impulse response data to the first processing unit. The first processing unit then zero-pads the truncated channel impulse response data and performs a frequency transform on the zero-padded channel impulse response data to obtain a three-dimensional channel matrix. In one case, the first processing unit may be the transmitter and the second processing unit  
20 may be the receiver. In a second case, the first processing unit may be the receiver and the second processing unit may be the transmitter.

**[0075]** Referring now to Figure 5a, shown therein is an alternative SVD-based OFDM-MIMO communication system **100** having a transmitter **112** and a receiver **216**. The functionality of the transmitter **112** is similar to the  
25 transmitter **12** and the functionality of the receiver **216** is similar to the receiver **16**. Accordingly, both the partial SVD algorithm **50** and the process **70** for generating the channel related data using truncated impulse responses is utilized by both transmitter/receiver sets of communication systems **10** and **100** as is the use of OFDM synchronization, data estimation, channel training  
30 symbols for channel estimation and subspace training symbols for subspace tracking. Accordingly, components which are common to both transmitters **12**

- 27 -

and 112 have reference labels that are offset by 100 and components that are common to both receivers 16 and 216 have reference labels that are offset by 200.

**[0076]** The fine partition of the communication channel in frequency  
5 (due to the use of OFDM) and spatial-subspaces (due to the use of SVD-based MIMO) enables the implementation of sophisticated adaptive algorithms for the communication system 100 at the sub-carrier and spatial-subspace level. For instance, adaptive subspace allocation, adaptive subspace coding, adaptive power allocation, and adaptive modulation may be  
10 used so that at any time, the available channel resources are preferably utilized optimally for the communication system 100. The receiver 216 determines transmission parameters related to spatial-subspace channel allocation, spatial-subspace channel coding, power allocation and modulation based on the subspace quality information and provides these transmission  
15 parameters to the transmitter 112. As mentioned previously, the receiver 216 also provides channel information to the transmitter 112. Accordingly, the data transmission protocol of the communication system 100 is adaptive in time, frequency and space.

**[0077]** Referring now to Figure 5b, the transmitter 112 comprises a first  
20 communication device 102 that provides an input data bit stream  $\mathbf{x_b}$  comprising binary data to a transmitter data pump 104. The first communication device 102 may be a computer, router or other electronic communication device. The transmitter data pump 104 is a hardware unit that is responsible for routing data to various units in the transmitter 112. A  
25 subspace allocation unit 120 receives the input data bit stream  $\mathbf{x_b}$  from the transmitter data pump 104 and transmission parameters from a transmitter adaptation unit 122. The subspace allocation unit 120 uses the transmission parameters for allocating an input data symbol stream  $\mathbf{x_k}$ , derived from the input data bit stream  $\mathbf{x_b}$ , on various spatial-subspace channels for a sub-  
30 carrier  $\mathbf{k}$ . A first data mapper unit 106 applies a particular modulation scheme, specified by the transmitter link adaptation unit 122, to the input data bit

- 28 -

stream  $\mathbf{x}_b$  to generate the input data symbol stream  $\mathbf{x}_k$  (which in general comprises complex data symbols) and provides the input data symbol stream  $\mathbf{x}_k$  to the subspace allocation unit 120. The subspace allocation unit 120 provides at least a portion of the transmission parameters to the first data  
5 mapper unit 106 for specifying the modulation scheme and the modulation order (i.e. modulation rate).

[0078] The transmission parameters used by the subspace allocation unit 120 include information on spatial-subspace channel allocation, spatial-subspace channel coding and the spatial-subspace channel modulation.  
10 These parameters are based on the subspace quality information for the associated channel matrix  $\mathbf{H}_k$ . The spatial-subspace channel allocation information indicates which spatial-subspace channels can support data transmission using a desired modulation order. The spatial-subspace channel coding information indicates whether coding should be used to combine two  
15 spatial-subspace channels for transmitting data. Spatial-subspace channels of various quality, such as two strong spatial-subspace channels, two weak spatial-subspace channels or a weak and a strong spatial-subspace channel could be combined using coding. Accordingly, the resulting spatial-subspace channels may be orthogonal to each other or the spatial-subspace channels  
20 may be dependent on one another (via coding) or there may be a combination of orthogonal and dependent spatial-subspace channels for a given sub-carrier  $k$ .

[0079] The spatial-subspace channel modulation information, provided to the first data mapper unit 106, indicates the modulation scheme that should  
25 be used on each spatial-subspace channel. The modulation scheme which can be used can vary from QAM to Phase Shift Keying (PSK) and Binary Phase Shift Keying (BPSK) with various modulation orders such as 64QAM, 32QAM, 16QAM, 4QAM, QAM, 64QPSK, 32QPSK, 16QPSK, 4QPSK, QPSK, BPSK, or other appropriate forms of modulation as is commonly known to  
30 those skilled in the art. The higher rates of modulation are used for stronger spatial-subspace channels, since the data points in the constellations

- 29 -

corresponding to higher modulation rates are closer together and require a channel with a better signal to noise ratio for minimizing data transmission errors. In each case, the signal to interference and noise ratio (SINR) for a spatial-subspace channel can be examined to ensure that a certain bit-error rate (BER) is maintained during transmission on a particular spatial-subspace channel or a plurality of coded spatial-subspace channels. The SINR for a spatial-subspace channel will depend on the magnitudes of the singular value and the noise and interference associated with that spatial-subspace channel.

[0080] Alternatively, the subspace allocation unit 120 and the first data mapper unit 106 can work in unison for a joint mapping and allocation of the input data symbol stream  $x_k$  according to an inter-spatial-subspace channel multi-resolution modulation scheme. The inter-spatial-subspace channel multi-resolution modulation scheme, for a given modulation scheme, specifies that the input data symbols that are the furthest apart from each other in the corresponding constellation, are allocated to weaker spatial-subspace channels. For instance, the input data symbols may be at the four corners of the constellation. Since the input data symbols are spaced far apart from one another in the constellation, these input data symbols may be placed in weaker spatial-subspace channels where it should still be possible to distinguish these input data symbols from one another despite noise corruption during data transmission. In contrast, the input data symbols that are spaced closer together in the constellation for the modulation scheme, are allocated to the stronger spatial-subspace channels. For instance, the input data symbols may be at the center of the constellation. Since the input data symbols are spaced close together, stronger spatial-subspace channels which have a larger SINR are needed since it will not take as much noise to cause these input data symbols to interfere with one another as it would for input data symbols that are positioned at the four corners of the constellation. The advantage of the inter-spatial-subspace channel multi-resolution modulation scheme is reduced processing complexity since the same constellation size (i.e. modulation rate or order) is used for both strong and weak spatial-subspace channels.

- 30 -

[0081] The subspace allocation unit 120 provides a plurality of input data symbol sub-streams with each data symbol sub-stream being allocated to a spatial-subspace channel. In general, there are two categories of input data symbol sub-streams: " $q_k$ " input data symbol sub-streams that are allocated on coded spatial-subspace channels and " $r_k$ " input data symbol sub-streams that are allocated on uncoded spatial-subspace channels, where  $r$  and  $k$  are integers that are greater than or equal to 0. The input data symbols received from the first data mapper unit 106 that are assigned to the coded spatial-subspace channels are represented by  $x_c$  and the input data symbols that are assigned to the uncoded spatial-subspace channels are represented by  $x_u$ .

[0082] The number of consecutive input data symbols that are processed at a time depends on the type of coding which is done on the spatial-subspace channels. For instance, if block space-time coding is used for coding the spatial-subspace channels, then two consecutive input data symbols are preferably processed at a time. In this case, the subspace allocation unit 120 preferably allocates the input data symbol sub-streams in the following fashion: a) a first data symbol sub-stream comprises two input data symbols  $x_{u_k}(1)$  and  $x_{u_k}(2)$  that are allocated on the first spatial-subspace channel which is uncoded, b) a second data symbol sub-stream comprises two input data symbols  $x_{u_k}(3)$  and  $x_{u_k}(4)$  that are allocated on the second spatial-subspace channel which is uncoded and c) a third data symbol sub-stream comprises two input data symbols  $x_{c_k}(1)$  and  $x_{c_k}(2)$  that are allocated on the third and fourth spatial-subspace channels which are coded. However, there could be other forms of coding in which more than two input data symbol sub-streams are coded and there are a corresponding number of coded spatial-subspace channels.

[0083] The subspace allocation unit 120 provides the input data symbol sub-streams to an encoder unit 108. The encoder unit 108 possibly codes the input data symbol sub-streams thereby producing uncoded/coded input data symbol sub-streams  $x_{s_{k1}}$ ,  $x_{s_{k2}}$ ,  $x_{s_{k3}}$  and  $x_{s_{k4}}$ . Accordingly, the

- 31 -

uncoded/coded input data symbol sub-streams may possibly comprise at least one uncoded input data symbol sub-stream for allocation on a corresponding at least one uncoded spatial-subspace channel and may possibly comprise at least one pair of coded input data symbol sub-streams for allocation on a corresponding at least one pair of coded spatial-subspace channels. In this example, there are four spatial-subspace channels with two of the channels being uncoded and two of the channels being coded. In general, there are several possibilities for the spatial-subspace channels. For instance, each spatial-subspace channel may be uncoded or there may be at least one spatial-subspace channel that is uncoded with the remaining pairs of spatial-subspace channels being coded. Alternatively, there may only be coded spatial-subspace channels.

**[0084]** The transmitter adaptation unit 122 is connected to the encoder unit 108 to provide transmission parameters that indicate which spatial-subspace channels are uncoded and which are coded. The encoder unit 108 simply passes the input data symbol sub-streams  $x_u$  which are to be sent on the uncoded spatial-subspace channels  $s_{k1}$  and  $s_{k2}$  and processes the input data sub-streams  $x_c$  that are to be sent on the coded spatial-subspaces  $s_{k3}$  and  $s_{k4}$  (in this example). The encoder unit 108 preferably uses block space-time coding with a depth of two input data symbols (as shown in Table 1) to create an equivalent channel from two spatial-subspace channels such that a desired BER is maintained for a given modulation scheme. Alternatively, other forms of coding may be used such as space-frequency coding or time-frequency coding (both of these forms of coding are commonly known to those skilled in the art).

Table 1. Space-Time block encoding

Data symbol	Spatial-subspace channel 3	spatial-subspace channel 4
$xc_k(1)$	$xc_k(1)$	$xc_k(2)$
$xc_k(2)$	$-xc_k^*(2)$	$xc_k^*(1)$

Note:  $xc_k^*(1)$  is the complex conjugate of  $xc_k(1)$ .



[0085] The subspace training unit 132 receives the coded/uncoded input data symbol sub-streams  $\mathbf{x}_{s_{k1}}$ ,  $\mathbf{x}_{s_{k2}}$ ,  $\mathbf{x}_{s_{k3}}$  and  $\mathbf{x}_{s_{k4}}$  from the encoder unit 108 and interleaves subspace training symbols into the coded/uncoded input data symbol sub-streams  $\mathbf{x}_{s_{k1}}$ ,  $\mathbf{x}_{s_{k2}}$ ,  $\mathbf{x}_{s_{k3}}$  and  $\mathbf{x}_{s_{k4}}$  thereby producing input data/training symbol sub-streams  $\mathbf{x}'_{s_{k1}}$ ,  $\mathbf{x}'_{s_{k2}}$ ,  $\mathbf{x}'_{s_{k3}}$  and  $\mathbf{x}'_{s_{k4}}$ . Accordingly, the subspace training unit 132 is connected to a training unit 130 to receive the subspace training symbols. The subspace training symbols are interleaved into the coded/uncoded input data symbol sub-streams in an uncoded manner. The subspace training symbols are preferably used to track one spatial-subspace channel at a time.

[0086] A power allocation unit 134 is connected to the subspace training unit 132. The power allocation unit 134 receives the input data/training symbol sub-streams  $\mathbf{x}'_{s_{k1}}$ ,  $\mathbf{x}'_{s_{k2}}$ ,  $\mathbf{x}'_{s_{k3}}$  and  $\mathbf{x}'_{s_{k4}}$  and weights each of these sub-streams with a corresponding power coefficient  $\alpha_1$ ,  $\alpha_2$ ,  $\alpha_3$  and  $\alpha_4$  to obtain power-weighted sub-streams  $\alpha_1 \mathbf{x}'_{s_{k1}}$ ,  $\alpha_2 \mathbf{x}'_{s_{k2}}$ ,  $\alpha_3 \mathbf{x}'_{s_{k3}}$  and  $\alpha_4 \mathbf{x}'_{s_{k4}}$ . The power allocation unit 134 is connected to the transmitter adaptation unit 122 in order to receive the portion of the transmission parameters that provides information on spatial-subspace channel power weighting.

[0087] Many different power allocation schemes may be implemented by the power allocation unit 134 under the direction of the transmitter link adaptation unit 122. For instance, one spatial-subspace channel may have a much higher SINR than is required for a certain data modulation scheme in which case a portion of the transmitter power may be routed from this spatial-subspace channel to the other spatial-subspace channels for the same sub-carrier  $k$ . Other power allocation methods include the water-filling method in which more power is allocated to the strongest spatial-subspace channels. Alternatively, the power allocation coefficients can be based on the average singular value amplitude per spatial-subspace channel across all sub-carriers. This technique reduces the computational demand at the receiver 216 and the amount of data that needs to be transmitted back to the transmitter 112.

- 33 -

[0088] The transmitter weighting unit 124 receives the power-weighted sub-streams  $\alpha_1 \mathbf{x} \mathbf{s}'_{k1}$ ,  $\alpha_2 \mathbf{x} \mathbf{s}'_{k2}$ ,  $\alpha_3 \mathbf{x} \mathbf{s}'_{k3}$  and  $\alpha_4 \mathbf{x} \mathbf{s}'_{k4}$  and further weights these sub-streams with transmitter weights to produce transmit-weighted spatial-subspace data. As explained previously for transmitter 12, the transmitter weighting unit 124 multiplies the power-weighted sub-streams with complex weighting values provided by the transmit weight matrix  $\mathbf{V}_k$  in accordance with equation 5 for diagonalizing the channel matrix  $\mathbf{H}_k$  for the sub-carrier  $k$ . Accordingly, via multiplication with the transmit weight matrix  $\mathbf{V}_k$ , the transmit-weighted spatial-subspace data is now distributed along the various spatial-subspace channels for the sub-carrier  $k$  and assigned to each element of the transmitter antenna array 114. This processing is applied to all of the sub-carriers.

[0089] The transmit weight matrix  $\mathbf{V}_k$  is calculated by the transmitter SVD unit 128 and provided to the transmitter weighting unit 124. The transmitter SVD unit 128 calculates the transmit weight matrix  $\mathbf{V}_k$  from the corresponding channel matrix  $\mathbf{H}_k$  which is provided by the transmitter link adaptation unit 122. The transmitter link adaptation unit 122 preferably computes the channel matrix  $\mathbf{H}_k$  in the same fashion described previously for the transmitter link adaptation unit 22 using truncated channel impulse response data.

[0090] A transmitter channel unit 136 receives the transmit-weighted spatial-subspace data from the transmitter weighting unit 124 and interleaves channel/transmission information (CTI) and channel training sequences into the transmit-weighted spatial-subspace data thereby producing interleaved spatial-subspace data for transmission to the receiver 216. The channel training symbols are provided by the training unit 130. The channel training sequences are inserted periodically into the transmit-weighted spatial-subspace data so that the receiver 216 can estimate the channel matrices  $\mathbf{H}_k$ . The channel training sequences may also be intermittently inserted for providing synchronization between the transmitter 112 and the receiver 216 (as described below).

- 34 -

**[0091]** The channel/transmission information is inserted into the transmit-weighted spatial-subspace data because the communication system **10** is bi-directional. The transmitter **112** and the receiver **216** actually function as transceivers in a frequency division duplex fashion in which OFDM data waveforms are sent from the transmitter **112** to the receiver **216** in a first frequency range and OFDM data waveforms are sent from the receiver **216** to the transmitter **112** in a second frequency range to increase the rate of data transmission for the communication system **100**. Accordingly, the channel matrices  $H_k$  must be estimated in both directions and the corresponding matrices  $U_k$  and  $V_k$  for each channel matrix  $H_k$  must be updated at both the transmitter **112** and the receiver **216** for both frequency ranges. The transceiver aspect of the transmitter **112** and the receiver **216** is not emphasized for simplifying the description of the communication system **100**. Accordingly, channel/transmission information (CTI) for the OFDM channel from the receiver **216** to the transmitter **112** is measured at the transmitter **112** (in a similar manner to the channel measurement which occurs at the receiver **216**) and the channel/transmission information is provided to the transmitter data pump **104**. The transmitter data pump **104** is connected to a second data mapper unit **138** which modulates the channel/transmission information using any appropriate modulation scheme as is commonly known to those skilled in the art. The second data mapper unit **138** then provides the modulated channel/transmission information to the transmitter channel unit **136**. Alternatively, the system **100** may also operate in a time division duplex manner in which case the channel matrix  $H_k$  for each sub-carrier  $k$  is symmetrical (i.e. there is no need to feedback the channel information from the transmitter to the receiver; only transmission information need be transmitted).

**[0092]** The interleaved spatial subspace data is partitioned into blocks of data before transmission to the receiver **216**. The channel training symbols are provided in a first portion of the block of data for allowing the communication system **100** to periodically estimate the channel matrices  $H_k$ . The data in each data block is further partitioned into a plurality of data sub-

- 35 -

blocks. Synchronization symbols, channel/transmission information and subspace training symbols are interleaved with the transmit-weighted spatial-subspace data in each of the data sub-blocks. The structure of the data blocks and data sub-blocks are described in more detail below.

5 [0093] The transmitter channel unit 136 provides the interleaved spatial-subspace data to the IFFT unit 126. The IFFT unit 126 converts the interleaved spatial-subspace data to the time domain thereby producing data symbol waveforms comprising OFDM data symbols. The RF unit 140 processes the data symbol waveforms for RF transmission by the transmitter  
10 antenna array 114. Accordingly, the RF unit 140 comprises hardware for performing digital-to-analog conversion and RF up-conversion to increase the center frequency of the data symbol waveforms. The RF unit 140 may further comprise hardware for interpolating and filtering the data symbol waveforms as is commonly known to those skilled in the art.

15 [0094] Referring now to Figure 5c, the receiver 216 comprises a receiver antenna array 218 which receives the data symbol waveforms. An RF unit 220 is connected to the receiver antenna array 218 and processes the data symbol waveforms by RF down-converting these waveforms and performing analog to digital conversion to produce received data symbol  
20 waveforms. The received data symbol waveforms are in the time domain. . An FFT unit 232, connected to the RF unit 220, processes the received data symbol waveforms to provide received spatial-subspace data which is frequency domain data. The FFT unit 232 and the RF unit 220 are also connected to a first multiplexer MUX1 in order to provide the received data  
25 symbol waveforms and the received spatial-subspace data as input data to the first multiplexer MUX1. After the FFT operation, the receiver processing is performed for all sub-carriers individually.

[0095] The multiplexer MUX1 provides either the received data symbol waveforms or the received spatial-subspace data to the channel estimation  
30 unit 236. When the transmitter 112 first begins to send data symbol waveforms to the receiver 216, the receiver 216 must be synchronized to the

- 36 -

transmitter **112** in order for the FFT unit **232** to be able to correctly process the received data symbol waveforms. Accordingly, the channel estimation unit **236** processes at least a portion of the received data symbol waveforms to provide a synchronization signal for the FFT unit **232**. A synchronization unit **222**, connected to the channel estimation unit **236**, receives the synchronization signal determines a timing offset parameter. The timing offset parameter is then provided to the FFT unit **232**.

[0096] The channel estimation unit **236** preferably employs a correlation-based synchronization method to recognize repetitive patterns in the received data symbol waveforms (recall that the transmitter **112** inserted synchronization sequences having repetitive patterns into the data that was transmitted). The synchronization process is performed at various times during the operation of the communication system **100**. The channel estimation unit **236** preferably calculates the cross-correlation coefficient between two samples spaced a certain number of samples apart in the synchronization sequences. This is repeated over several samples as is commonly known by those skilled in the art. The resulting cross-correlation sequence has a maximum value at a time sample **G** which corresponds with the end of the repetitive synchronization sequence. The synchronization unit **222** receives the index of time sample **G** and calculates the timing offset parameter which is then provided to the FFT unit **232**.

[0097] As mentioned previously in the description of the transmitter **112**, the data symbol waveforms that are transmitted also contain channel and transmission information (CTI). Accordingly, the receiver **216** comprises a CTI symbol demodulator **224**, connected to the FFT unit **232**, that demodulates the CTI information in the received spatial-subspace data. The CTI symbol demodulator **224** performs a decoding/detection process based on the modulation scheme that is used by the second data mapper **138** in the transmitter **112**. A super-frame detector **226**, connected to the CTI symbol demodulator **224**, analyzes the demodulated CTI information to determine whether a new super-frame (discussed below) of OFDM spatial-subspace

- 37 -

data is being received by the receiver 216. The super-frame detector 226 may use a correlation technique with a programmable threshold for detecting each new OFDM super-frame. The beginning of each OFDM super-frame contains channel training signals. Accordingly, the super-frame detector 226 is  
5 connected to the channel estimation unit 236 and the multiplexer MUX1 to indicate the detection of a new OFDM super-frame. When the beginning of an OFDM super-frame is detected, the multiplexer MUX1 provides the received spatial-subspace data to the channel estimation unit 236 which then estimates the set of channel matrices  $H_k$  as described further below.

10 [0098] A receiver SVD unit 240, connected to the channel estimation unit 236, performs the SVD operation on the estimated channel matrices  $H_k$ , in accordance with the partial SVD algorithm described previously, to obtain the triplet of matrices  $V_k$ ,  $\Lambda_k$  and  $U_k^*$  for each sub-carrier  $k$ . A receiver weighting unit 234, connected to the receiver SVD unit 240, then applies the  
15 weights in the matrix  $U_k^*$  to the received spatial-subspace data to provide receive-weighted spatial-subspace data. The receiver SVD unit 240 is also connected to a receiver link adaptation unit 242 to provide an initial estimate of the singular value matrix  $\Lambda_k$ .

[0099] A second multiplexer MUX2, connected to the receiver  
20 weighting unit 234, routes the receive-weighted spatial-subspace data to either a data estimator unit 238 or the receiver link adaptation unit 242. As mentioned previously in the description of the transmitter 112, the receive-weighted spatial-subspace data comprises, in part, input data symbols and subspace training symbols. When the receive-weighted spatial-subspace data  
25 comprises subspace training signals, the receiver link adaptation unit 242 processes the subspace training signals for tracking the subspace variation in the singular value matrix  $\Lambda_k$ . When the receive-weighted spatial-subspace data comprises input data symbols, the data estimation unit 238 processes the received-weighted spatial-subspace data for estimating output data that is  
30 related to the input data bits  $x_b$ . The estimation may include detection and

- 38 -

decoding and the output data may be a data bit stream or a stream of data symbols with associated confidence levels (as discussed further below).

**[00100]** A receiver data pump **244**, connected to the data estimation unit **238** and the receiver link adaptation unit **242**, routes data and other  
5 information to various units in the receiver **216**. In particular, the data estimation unit **238** is connected to a data interface **246**. The data interface **246** receives the estimated output data and provides this data to a second communication device **248**. The second communication device **248** may be a computer, router or the like.

**[00101]** The receiver link adaptation unit **242** comprises a subspace matrix tracker **228** and a transmission and channel information unit **230**. The subspace matrix tracker **228** receives an initial estimate of the singular value matrix  $\Lambda_k$  from the receiver SVD unit **240**. The subspace matrix tracker **228** also processes the subspace training symbols in the receive-weighted spatial-  
15 subspace data, received from the multiplexer **MUX2**, for periodically updating the singular value matrix  $\Lambda_k$  as described further below. The subspace matrix tracker **228** is also connected to the data estimation unit **238** for providing the initial estimate of the singular value matrix  $\Lambda_k$  and the values in the updated singular value matrix  $\Lambda_k$ .

**[00102]** The transmission and channel information unit **230** is connected to the subspace matrix tracker **228** to receive the initial estimate of the singular value matrix  $\Lambda_k$  for determining subspace quality information for each sub-carrier at the beginning of an OFDM super-frame. The transmission and channel information unit **230** calculates the transmission parameters based on  
25 the subspace quality information. The transmission and channel information unit **230** is also connected to the channel estimation unit **236** to receive channel related data. The transmission and channel information unit **230** combines the transmission parameters and the channel related data into channel/transmission information (CTI). The transmission and channel  
30 information unit **230** is further connected to a transmission interface **250** of the receiver data pump **244**. The transmission interface **250** receives the

- 39 -

channel/transmission information from the transmission and channel information unit 230 and routes this information to the transmission portion of the receiver 216, which is similar to the transmitter 112, (recall that the transmitter 112 and the receiver 216 are transceivers) for transmitting the  
5 channel/transmission information to the transmitter 112.

**[00103]** The receiver link adaptation unit 242 determines the transmission parameters which include spatial-subspace channel allocation, spatial-subspace channel coding, spatial-subspace channel modulation and spatial-subspace channel power weighting. As mentioned previously, each  
10 transmission parameter is determined by examining the signal to interference and noise ratio (SINR) for each spatial-subspace channel for a particular sub-carrier  $k$ . A particular combination of spatial-subspace channel allocation, spatial-subspace channel coding, spatial-subspace channel modulation and spatial-subspace channel power weighting can be selected based on the  
15 SINR and a desired BER for a given spatial-subspace channel or for a given plurality of coded spatial-subspace channels.

**[00104]** Referring now to Figure 6a, shown therein is the data structure 300 used by the communication system 100 for transmitting data. At the transmitter 112, the input data symbol stream is divided into a plurality of  
20 OFDM super-frames of which three are shown 302, 304 and 306. Each OFDM super-frame comprises a first channel training block 308 which contains channel training symbols and a plurality of OFDM frames of which three are shown 310, 312 and 314. There are  $N_F$  OFDM frames in each OFDM super-frame. In general, each OFDM frame comprises a slot for a  
25 training/synchronization symbol 316 (i.e. either a training symbol, a synchronization symbol or a training/synchronization symbol (i.e. a symbol used both for training and synchronization)), a slot for a channel/transmission information (CTI) symbol 318 and a plurality of slots for OFDM data symbols for carrying data, of which three are shown 320, 322 and 324. There are  $N_S$   
30 OFDM data symbols in an OFDM frame. These symbols may be OFDM symbols in which all the OFDM sub-carriers are used for a particular purpose,



- 40 -

i.e. channel training, subspace training, synchronization, channel/transmission information or data. Alternatively, these symbols may be sequences in which a portion of the entire set of sub-carriers is used for a particular purpose. In this case, it could be more generally stated that each OFDM frame comprises

5 a slot for a training/synchronization sequence (i.e. at least one of or a combination of a channel training sequence, a subspace training sequence, a synchronization sequence or a training/synchronization sequence (i.e. a sequence used both for training and synchronization)), a slot for a channel/transmission information (CTI) sequence and a plurality of slots for

10 data sequences. Accordingly, some of these sequences may be combined into an OFDM symbol. In another sense, the slots may contain at least a portion of each of these sequences depending on the length of these sequences and the number of sub-carriers.

**[00105]** Each OFDM symbol preferably comprises a guard portion

15 having duration  $T_G$  seconds and a useful information portion having duration  $T_U$  seconds. Accordingly, the total duration of an OFDM symbol is  $T_S = T_U + T_G$  seconds. The guard portion is used to mitigate intersymbol interference as is commonly known to those skilled in the art. The guard portion may be a cyclic prefix representing a copy of the end of the information portion of the OFDM

20 data symbol.

**[00106]** In general, an OFDM symbol can be one of: a) a training symbol, b) a synchronization symbol, c) a training/synchronization symbol, d) a channel/transmission information symbol CTI and e) a data symbol. The training/synchronization symbol 316 can be a subspace training symbol that is

25 used for subspace tracking or a synchronization symbol that is used for synchronization. In some cases, an OFDM frame may not have a training symbol or a CTI symbol (discussed further below). The length of an OFDM frame and an OFDM super-frame is selected to meet requirements such as time stability of the channel, frequency stability of the reference source and

30 control information bandwidth.

- 41 -

[00107] The channel training block 308 is sent at the beginning of each OFDM super-frame for periodically estimating the communication channel. The length of the OFDM super-frame is chosen based on the time wide-sense stationarity of the communication channel. Each channel matrix  $H_k$  is estimated, the corresponding triplet of matrices  $U_k$ ,  $\Lambda_k$  and  $V_k$  are estimated and the channel related data is then calculated. The receiver link adaptation unit 242 then calculates the transmission parameters and provides the channel/transmission information (CTI). These matrices, channel related data and transmission parameters are used for the data transmission that occurs during the next OFDM super-frame. Accordingly, during the first OFDM super-frame, no data symbols are sent. Further, the matrices  $U_k$  and  $V_k$  and the transmission parameters remain fixed during the next OFDM super-frame. However, the estimated singular value matrix  $\Lambda_k$  is used only during a first portion of the next OFDM super-frame and is updated periodically during the remainder of the next OFDM super-frame (as discussed below).

[00108] Referring now to Figure 6b, shown therein is a table showing the elements of an exemplary channel training block. This example assumes that there are 8 transmitter antenna elements as shown in the first column labeled TX. To estimate the channel matrices  $H_k$ , a plurality of channel training symbols HT are sent from each transmitter antenna element to all of the receiver antenna elements in a time-division manner which allows for the row-wise construction of each channel matrix  $H_k$ . For example, when transmitter antenna element 1 sends the channel training symbols HT, the first row of each channel matrix  $H_k$  can be estimated. Alternatively, rather than strictly using a time-division approach and transmitting from one transmitter antenna element at a time, a combination of time-division and frequency-division may be used in which all transmitter antenna elements transmit at the same time, however, different transmitter antenna elements transmit on different OFDM sub-carriers. For instance, in a first time duration, transmitter antenna element 1 may transmit on OFDM sub-carriers at frequency indices 1, 9, 17, etc., transmitter antenna element 2 may transmit on OFDM sub-carriers at

- 42 -

frequency indices 2, 10, 18, etc., and so on. In the next time duration, transmitter antenna element 1 may transmit on OFDM sub-carriers at frequency indices 2, 10, 18, etc., transmitter antenna element 2 may transmit on OFDM sub-carriers at frequency indices 3, 11, 19, etc., and so on. This process may be repeated 8 times so that each transmitter antenna element transmits on each OFDM sub-carrier. Alternatively, interpolation may be used in the frequency domain so that each transmitter antenna need not transmit on each OFDM sub-carrier. Another approach is to transmit orthogonal training sequences in the time domain on all transmitter antenna elements at the same time and then separate the orthogonal training sequences at the receiver using correlation. Yet another approach is to use a single training sequence in which the training sequence is shifted by a different amount at each of the transmitter antenna elements, and correlation is used at the receiver to recover the shifted training sequences.

[00109] As shown in Figure 6b, in the time-division only channel training approach, a plurality of the channel training symbols HT are preferably repeatedly transmitted by each antenna element in the transmitter antenna array 114. This allows for averaging the responses at the receiver 216 when constructing each channel matrix  $H_k$  for noise reduction. This is advantageous since the accuracy of channel estimation is affected by noise and quantization error in the receiver 216. In this example, four channel training symbols are sent which provides for a noise reduction of 6 dB in the estimation of each channel matrix  $H_k$ . A larger or smaller number of training symbols may be repeatedly sent by each transmitter antenna depending on the amount of data/time that can be used for channel estimation.

[00110] As mentioned previously, the channel training symbol HT is an OFDM symbol that preferably has a low peak-to-average power ratio in which some of the sub-carriers have a magnitude of zero. More specifically, the channel training symbol HT can be a pseudo-noise sequence in the frequency domain in which every even numbered sub-carrier has a magnitude of either +1 or -1 and every odd numbered sub-carrier has a magnitude of 0. This type

- 43 -

of frequency domain sequence has the property of repeating itself twice in the time domain. Accordingly, this frequency domain sequence can also be used for timing synchronization, as is commonly known by those skilled in the art. Accordingly, the channel training symbol **HT** may be used for both channel  
5 estimation, in the channel training block **308** of each OFDM super-frame, and synchronization, in the training/synchronization symbol **316**, of each OFDM frame. The channel training symbol **HT** may also be used for subspace matrix tracking in which case the channel training symbol **HT** is multiplied by the weighting matrix  $\mathbf{V}_k$  to provide a subspace training symbol  $\Delta\mathbf{T}$ . The channel  
10 training symbol **HT** is preferably modulated by BPSK prior to transmission. Alternatively, another low-order modulation scheme may be used.

[00111] The channel training symbol **HT** is modified by the communication channel  $\mathbf{H}_k(\mathbf{b}, \mathbf{c})$  between the transmitting antenna element **b** that sends the channel training symbol **HT** and the receiver antenna element  
15 **c** that receives the modified channel training symbol. At the receiver **216**, after FFT processing for the receiver antenna element **c**, the channel estimation unit **236** receives the modified channel training symbol and multiplies it with the original training symbol **HT** to produce a processed channel training symbol that contains the frequency response of the communication channel  
20  $\mathbf{H}_k(\mathbf{b}, \mathbf{c})$ . This multiplication procedure has the effect of removing the BPSK modulation (i.e. +1 or -1) of the modified channel training symbol. Interpolation is then performed on the processed channel training symbol to determine the amplitudes of the odd sub-carrier components of the channel frequency response. This procedure is repeated for each combination of the  
25 transmitter and receiving antenna elements to obtain the three-dimensional frequency response matrix **60** shown in Figures 3a and 3c.

[00112] Referring now to Figure 6c, shown therein is the format of a CTI symbol which carries the channel/transmission information. Each CTI symbol comprises a header portion and an information portion. The header portion of  
30 the CTI symbol contains a unique identifier that signifies the start of an OFDM super-frame if the CTI symbol is in the first frame of an OFDM super-frame

- 44 -

(recall that the detection of the first OFDM super-frame is performed by the super-frame detector 226). Otherwise, the header portion of the CTI symbol contains the OFDM frame index (which may be repeated in the header portion for robustness). Accordingly, the header portion of the CTI symbol is used for  
5 super-frame synchronization. The information portion of the CTI symbol contains the channel/transmission information which is modulated and may also include forward error correction.

[00113] The transmitter 112 and receiver 216 synchronize with one another: 1) when establishing a control channel at the beginning of system  
10 operation, 2) at the beginning of each OFDM super-frame (by detecting the super-frame header in the CTI symbols as discussed earlier), and 3) periodically in an OFDM super-frame during the transmission of the OFDM frames. In each of these instances, the channel training symbols HT may be used for correlation-based synchronization as described earlier.

15 [00114] The control channel must be established at the beginning of system operation. One of the transmitter 112 and the receiver 216 is considered a master and the other is considered a slave. At the beginning of system operation, the master transmits on the control channel by sending synchronization symbols via one of the antenna elements of the transmitter  
20 antenna array 114. The slave may receive the synchronization symbols on a single antenna element or on all antenna elements of the receiver antenna array 218 (in this case block space-time coding can be used on the control channel for increased robustness). The slave will attempt to synchronize with the synchronization signals. Once synchronization is achieved, the control  
25 channel is decoded and the slave can reply on the control channel to signal that a link is established between the master and the slave. The master can then establish the MIMO channels by transmitting the channel training block.

[00115] The synchronization process also takes into account the different propagation delays between transmission from the antenna elements  
30 of the transmitter antenna array 114 to the antenna elements of the receiver antenna array 218 periodically during an OFDM super-frame. Referring now

- 45 -

to Figure 6d, shown therein is a multiplexing scheme for distributing synchronization symbols **SY** for the synchronization of each OFDM frame and taking into account the different delays from each transmitter antenna. The synchronization symbols **SY** are sent separately by each antenna element of the transmitter antenna array **114** so that the different delays from each transmitter antenna element can be measured and compared. There are also blank intervals in which no synchronization symbols are sent in an OFDM frame (i.e. the blank columns in Figure 6d). However, other training symbols may be sent in these intervals as discussed below. The delay for transmission from each transmitter antenna element is measured indirectly by calculating the timing offset word associated with each transmitter antenna element (as described previously). The largest delay, represented by the largest timing offset parameter, is used for synchronization by the FFT unit **232** such that the largest delay spread falls within the guard portion of the OFDM symbols (it is desirable to perform the FFT as close as possible to the end of the guard interval). This measurement is performed periodically (every 12 OFDM frames in this example) and the largest timing offset parameter is preferably updated after the 12<sup>th</sup> OFDM frame (this measurement may alternatively be performed over shorter or longer time frames as desired).

**[00116]** The SVD-based MIMO model given in equations 1-5 assumes that the channel matrix  $H_k$  is perfectly known. However, in practice, only an estimate of the channel matrix  $\hat{H}_k$  is available where  $\hat{H}_k = H_k + \Delta H_k$ . The estimation error of  $\Delta H_k$  depends on quantization error, channel noise and the channel estimation method. Accordingly, the channel matrix  $H_k$  cannot be truly diagonalized mainly because the  $U_k$  and  $V_k$  matrices are computed from the matrix  $\hat{H}_k$  rather than the matrix  $H_k$ . This problem of matrix diagonalization is further compounded by the use of the partial SVD algorithm **50** (recall that the singular value matrix  $\Lambda_k$  is quasi-diagonal). Consequently, the received data symbol vector  $Y_k$  is given by equation 6 rather than equation 5.

$$Y_k = (\Lambda_k - U_k^* \Delta H_k V_k) X_k + U_k^* n_k \quad (6)$$

- 46 -

[00117] In order to detect the transmitted data symbol vector  $X_k$  from the received vector, the matrix  $\Lambda_{ek} = \Lambda_k - U_k^* \Delta H_k V_k$  should be known. The inventors have realized that the matrix  $\Lambda_{ek}$  can be obtained in the same way as  $\hat{H}_k$  (i.e. with the use of subspace training symbols  $\Delta T$ ), the only difference  
 5 being that for channel estimation, the channel training symbols  $HT$  are un-weighted, while for subspace tracking, the subspace training symbols  $\Delta T$  have to be weighted by the weights provided by the matrix  $V_k$ .

[00118] The estimation of the matrix  $\Lambda_{ek}$  is less computationally intensive than the estimation of the channel matrices  $H_k$  because the matrix  $\Lambda_{ek}$  is  
 10 smaller (i.e.  $\Lambda_{ek}$  has a dimension of  $p_k \times p_k$ ) than the channel matrix  $H_k$ . However, the matrix  $\Lambda_{ek}$  is "quasi-diagonal", meaning that the off-diagonal components are small but non-zero. These off-diagonal components represent inter-subspace interference. An example of the quasi-diagonal subspace matrix  $\Lambda_{ek}$  is shown in equation 7 for four subspaces.

$$15 \quad \Lambda_{ek} = \begin{bmatrix} \lambda_{11} & \lambda_{12} & \lambda_{13} & \lambda_{14} \\ \lambda_{21} & \lambda_{22} & \lambda_{23} & \lambda_{24} \\ \lambda_{31} & \lambda_{32} & \lambda_{33} & \lambda_{34} \\ \lambda_{41} & \lambda_{42} & \lambda_{43} & \lambda_{44} \end{bmatrix} \quad (7)$$

[00119] The columns of the matrix  $\Lambda_{ek}$ , for a sub-carrier  $k$ , can be determined by sending the subspace training symbols  $\Delta T$  on one spatial-subspace channel at a time. For example, the first row of the matrix  $\Lambda_{ek}$  can be determined by allocating the training symbols  $HT$  to the first spatial-subspace channel, weighting the training symbols  $HT$  by the transmit weight  
 20 matrix  $V_k$  at the transmitter 112 to produce the channel training symbols  $\Delta T$  and transmitting the channel training symbols to the receiver 216. The channel training symbols  $\Delta T$  are then weighted by the receive weight matrix  $U_k^*$  at the receiver 216 to provide values for the column in the quasi-diagonal  
 25 singular value matrix  $\Lambda_{ek}$  that corresponds to the first spatial-subspace channel. This is then repeated for each spatial-subspace channel.

- 47 -

**[00120]** Referring now to Figure 7a, shown therein is a data transmission scheme for sending the subspace training symbols  $\Delta T$  in the OFDM frames of an OFDM super-frame. Time division is used at the spatial-subspace channel level so that the subspace matrix tracker 228 knows which spatial-subspace channel is being estimated. There are gaps in which no subspace training symbols  $\Delta T$  are transmitted for providing the subspace matrix tracker 228 with an opportunity to estimate the column of the quasi-diagonal subspace matrix  $\Lambda_{ek}$ . After the last spatial-subspace channel is estimated, the singular value matrix  $\Lambda_{ek}$  is updated and used by the data estimation unit 238. This process is repeated throughout the OFDM super-frame. Accordingly, the singular value matrix  $\Lambda_{ek}$  is continuously being tracked and updated during an OFDM super-frame. In this example, the subspace training symbols  $\Delta T$  are spaced three OFDM frames apart. Furthermore, since there are four spatial-subspace channels in this example, the sequence of  $\Delta T$  training symbols repeat every 12 OFDM frames and the quasi-diagonal subspace matrix  $\Lambda_{ek}$  is updated every 12 OFDM frames. The subspace training symbols  $\Delta T$  are generated in the same fashion as the channel training symbols  $HT$  and are preferably modulated by BPSK. The subspace training symbols  $\Delta T$  can also be multiplied by the appropriate power coefficient  $\alpha_{k1}$ ,  $\alpha_{k2}$ ,  $\alpha_{k3}$  and  $\alpha_{k4}$  depending on the spatial-subspace channel that is being tracked.

**[00121]** Referring now to Figure 7b, shown therein is a data transmission scheme for sending the subspace training symbols  $\Delta T$  on each transmitter antenna element for subspace tracking. Following with the current example, in every 3<sup>rd</sup> OFDM frame, each transmitter antenna element sends the subspace training symbols  $\Delta T$  for a particular spatial-subspace channel. The gaps in the transmission of the subspace training symbols  $\Delta T$  can be used for the transmission of synchronization symbols  $SY$  for OFDM frame synchronization as shown in Figure 7c. It should be understood that the subspace training symbol  $\Delta T$  and the synchronization symbol  $SY$  occupy the training/synchronization symbol slot 316 in an OFDM frame (see Figure 6a).



- 48 -

**[00122]** Referring now to Figure 8, shown therein is an example of an overall data structure used by the communication system incorporating channel training symbols **HT**, subspace training symbols  $\Delta T$ , synchronization symbols **SY**, channel/transmission information **CTI** and data symbols **Di**. The matrices  $U_k^*$ ,  $V_k$  and  $\Lambda_k$  and the channel/transmission information **CTI** have been estimated in the prior OFDM super-frame for use in the current OFDM super-frame. At the beginning of the current OFDM super-frame, the channel training symbols **HT** are transmitted during the channel training block (it should be understood that each transmitter antenna element can send more than one channel training symbol **HT** for averaging to produce noise reduction). During the remainder of the current OFDM super-frame, the matrices  $U_k^*$ ,  $V_k$  and  $\Lambda_k$  and the channel/transmission information is being estimated for use in the next OFDM super-frame.

**[00123]** In the particular example shown in Figure 8, 14 OFDM data symbols **D1**, ..., **D14** are transmitted during each OFDM frame (although this can be increased or decreased as desired). Further, in OFDM frames 1 and 4, the subspace training symbols  $\Delta T$  are being sent for subspace tracking for updating the quasi-diagonal subspace matrix  $\Lambda_{ek}$  every 12 OFDM frames. In addition, channel/transmission information **CTI** is sent during every OFDM frame by the first transmitter antenna element and received by each receiver antenna element. In this fashion, space diversity can be used at the receiver **216** for improving the transmission of the channel/transmission information **CTI**. Alternatively, the channel/transmission information **CTI** may be transmitted by more than one transmitter antenna element. However, some orthogonality must be imposed on the channel/transmission information **CTI** sent by each transmitter antenna element so that the receiver **216** can properly receive the channel/transmission information.

**[00124]** Referring once more to Figure 5c, the data estimation unit **238** employs an iterative decoding/detection process for estimating output data that is related to the receive-weighted spatial-subspace data. Due to complexity, the iterative decoding/detection process is described for the

- 49 -

particular case of three spatial-subspace channels in which one spatial-subspace channel is uncoded and the other two spatial-subspace channels are space-time block coded. Further, for exemplary purposes, there are 8 transmitter antenna elements, 8 receiver antenna elements and 3 spatial-subspace channels for sub-carrier  $k$ , with the first spatial-subspace channel being uncoded and the second and third spatial-subspace channels being coded. After the FFT unit 232, an 8-element received data symbol vector for the sub-carrier  $k$  is multiplied by the  $3 \times 8$  receive weight matrix  $U^*_k$  to provide a  $3 \times 1$  receive-weighted data symbol vector. This is done for two consecutive received data symbol vectors for forming a  $2 \times 3$  receive-weighted data symbol matrix  $r_k$  that is the input to the data estimation unit 238 as given in equation 8.

$$r_k = \begin{bmatrix} r_{11} & r_{12} \\ r_{21} & r_{22} \\ r_{31} & r_{32} \end{bmatrix} \quad (8)$$

The first column ( $r_{11}$ ,  $r_{21}$ ,  $r_{31}$ ) is the uncoded and coded pair of receive-weighted data symbols respectively for the first receive-weighted data symbol vector and the second column ( $r_{12}$ ,  $r_{22}$ ,  $r_{32}$ ) is the uncoded and coded pair of receive-weighted data symbols respectively for the second receive-weighted data symbol vector.

**[00125]** In this example, the receive-weighted data symbols are decoded/detected in pairs (since they were transmitted as pairs at the transmitter 112 due to the block space-time coding applied to the coded spatial-subspace channels). The operations performed in each iteration of the iterative decoding/detecting process include: (1) decoding and detection of the receive-weighted coded data symbols that are transmitted on the coded spatial-subspace channels ignoring the interference from receive-weighted uncoded data symbols that are transmitted on the uncoded spatial-subspace channel, and (2) estimation and detection of the receive-weighted uncoded data symbols with the receive-weighted coded data symbols replaced by the values detected in step (1). The iterative decoding/detection process is

- 50 -

preferably completed in two iterations although more iterations may be used if desired. The detection performed in both steps preferably utilizes the maximum likelihood method.

**[00126]** The quasi-diagonal subspace matrix  $\Lambda_{ek}$  for the OFDM sub-carrier  $k$  is given by equation 9 for this example of three spatial-subspace channels. The quasi-diagonal subspace matrix  $\Lambda_{ek}$  is either the originally calculated subspace matrix or an updated version depending upon within which OFDM frame the decoding/detecting is being done.

$$\Lambda_{ek} = \begin{bmatrix} \lambda_{11} & \lambda_{12} & \lambda_{13} \\ \lambda_{21} & \lambda_{22} & \lambda_{23} \\ \lambda_{31} & \lambda_{32} & \lambda_{33} \end{bmatrix} \quad (9)$$

10

The first row of the quasi-diagonal subspace matrix  $\Lambda_{ek}$  represents the uncoded spatial-subspace channel and the second and third rows represent the coded spatial-subspace channels.

**[00127]** The decoding is performed according to equations 10 and 11 to obtain estimated receive-weighted coded data symbols  $e_c(1)$  and  $e_c(2)$ .

$$e_c(1) = \gamma (\lambda_{22}^* r_{21} + \lambda_{32}^* r_{31} + r_{22}^* \lambda_{23} + r_{32}^* \lambda_{33}) \quad (10)$$

$$e_c(2) = \gamma (\lambda_{23}^* r_{21} + \lambda_{33}^* r_{31} - r_{22}^* \lambda_{22} - r_{32}^* \lambda_{32}) \quad (11)$$

The coefficient  $\gamma$  is given by equation 12.

$$\gamma = \frac{1}{\|\lambda_{22}\|^2 + \|\lambda_{32}\|^2 + \|\lambda_{23}\|^2 + \|\lambda_{33}\|^2} \quad (12)$$

20 The value  $\lambda_{22}^*$  is the conjugate of  $\lambda_{22}$  and the value  $\|\lambda_{22}\|$  is the absolute value of  $\lambda_{22}$ . Estimated receive-weighted uncoded data symbols  $e_u(1)$  and  $e_u(2)$  are computed using equations 13 and 14 where  $\delta$  is given by equation 15.

$$e_u(1) = \delta (r_{11} - \lambda_{12} r_{21} - \lambda_{13} r_{31}) \quad (13)$$

$$e_u(2) = \delta (r_{12} - \lambda_{12} r_{22} - \lambda_{13} r_{32}) \quad (14)$$

- 51 -

$$\delta = \frac{\lambda_{11}^*}{\|\lambda_{11}\|^2} \quad (15)$$

- [00128]** Detection is performed on the estimated data symbols based on the maximum likelihood method which is well known by those skilled in the art. The modulation scheme used for creating the input data symbols at the transmitter 112 is specified by the receiver link adaptation unit 242. Prior to detection, the estimated receive-weighted coded and uncoded data symbols are power-weighted by coefficients  $\beta_1$ ,  $\beta_2$ , and  $\beta_3$ , which are the inverses of the adaptive power allocation coefficients  $\alpha_1$ ,  $\alpha_2$  and  $\alpha_3$ . The maximum likelihood method then produces detected receive-weighted uncoded and coded data symbols by determining which point in the associated constellation of the modulation scheme is closest to the power-weighted estimated receive-weighted uncoded and coded data symbols. The detected uncoded data symbols are  $d_u(1)$  and  $d_u(2)$  and the detected coded data symbols are  $d_c(1)$  and  $d_c(2)$ .
- [00129]** The following is a step-by-step description of the iterative decoding/detection process for the exemplary receive-weighted data symbol matrix  $r_k$  given by equation 8. During the first iteration:

Step 1: Load the symbol matrix  $r_k$  with the values in Table 2.

**Table 2**

Element	Value
$r_{11}$	$r_u(1)$
$r_{12}$	$r_u(2)$
$r_{21}$	$r_{c1}(1)$
$r_{22}$	$r_{c1}(2)$
$r_{31}$	$r_{c2}(1)$
$r_{32}$	$r_{c2}(2)$

20

The values  $r_u(1)$  and  $r_u(2)$  are respectively the first and second receive-weighted uncoded data symbols that are received on the first spatial-subspace channel which is uncoded. The values  $r_{c1}(1)$  and  $r_{c1}(2)$  are respectively the first and second receive-weighted coded data symbols that

- 52 -

are received on the second spatial-subspace channel which is coded. The values  $r_{c2}(1)$  and  $r_{c2}(2)$  are respectively the first and second receive-weighted coded data symbols that are received on the third spatial-subspace channel which is coded.

- 5 **Step 2:** Decode the receive-weighted coded data symbols using equations 10 to 12 and then detect the estimated receive-weighted coded data symbols using the maximum-likelihood method. The detected coded data symbols are  $d_c(1)$  and  $d_c(2)$ .

**Step 3:** Load the receive-weighted data symbol matrix  $r_k$  with the values in

10 Table 3.

**Table 3**

Element	Value
$r_{11}$	$r_u(1)$
$r_{12}$	$r_u(2)$
$r_{21}$	$d_c(1)$
$r_{22}$	$-d_c^*(2)$
$r_{31}$	$d_c(2)$
$r_{32}$	$d_c^*(1)$

- Step 4:** Estimate the receive-weighted uncoded data symbols using equations 13 to 15 and then detect the estimated receive-weighted uncoded data symbols using the maximum-likelihood method. The detected uncoded data symbols are  $d_u(1)$  and  $d_u(2)$ . The data symbol vector  $[d_u(1); d_u(2); d_c(1); d_c(2)]$  is the result of the first iteration of the iterative decoding/detection process.

- Step 5:** Apply the adaptive power allocation coefficients  $\alpha_i$  and the adaptive subspace coding to the symbols  $d_u(1)$ ,  $d_u(2)$ ,  $d_c(1)$ ,  $d_c(2)$  and load the receive-weighted data symbol matrix  $r_k$  with these processed values as shown in Table 4.

Table 4

Element	Value
$r_{11}$	$d_u(1)$
$r_{12}$	$d_u(2)$
$r_{21}$	$d_c(1)$
$r_{22}$	$-d_c^*(2)$
$r_{31}$	$d_c(2)$
$r_{32}$	$d_c^*(1)$

Step 6: Perform a second iteration of steps 2 to 5 on Table 4. These iterations comprise:

- 5                    6.1) Performing step 2
- 6.2) Saving  $e_c(1)$  and  $e_c(2)$
- 6.3) Performing steps 3 and 4
- 6.4) Saving  $e_u(1)$  and  $e_u(2)$

**[00130]**        The symbol vector  $[\beta_1 e_u(1); \beta_1 e_u(2); \beta_2 e_c(1); \beta_3 e_c(2)]$  is the result  
10   of the iterative decoding/detection process. The last operation is to recover  
the output data by de-mapping the detected uncoded and coded data  
symbols according to the modulation scheme that was originally used to  
produce the input data symbols prior to transmission. The output data may be  
obtained by using a de-mapping method that incorporates a hard decision  
15 (such as the maximum likelihood method for example) to provide output data  
bits **yb**. The data bits **yb** can then be provided to the data interface **246** of the  
receiver data pump **244**. Alternatively, a de-mapping method that uses a soft  
decision may be used to provide an output data symbol stream with  
associated confidence levels. In this case, the data interface **246** includes a  
20 decoder, such as a forward error decoder or the like, for determining the  
output data bits **yb** based on the output data symbol stream and the  
associated confidence levels.

**[00131]**        The iterative decoding/detection process can be applied to a  
wide variety of cases for the spatial-subspace channels for a given sub-carrier  
25 **k** such as: 1) there are only uncoded spatial-subspace channels, 2) there is a

- 54 -

combination of uncoded and coded spatial-subspace channels and 3) there are only coded spatial-subspace channels. In the first case, a system of independent equations is used for estimation in which the number of equations is equal to the number of uncoded spatial-subspace channels.

5 Each of these independent equations would be similar to equations 13 to 15. Alternatively, if at least one pair of coded spatial-subspace channels is used for data transmission, then the iterative decoding/detection process begins with decoding the receive-weighted coded data symbols using equations based on equations 10 to 12. The estimated receive-weighted coded data

10 symbols are then detected, via the maximum likelihood method for example, to obtain the detected coded data symbols and the receive-weighted coded data symbols are then replaced with the detected coded data symbols. If there are more than one pair of coded spatial-subspace channels then decoding/detection is first performed on the pair of coded spatial-subspace

15 channels with the stronger SINR (i.e. larger magnitude singular values) and then performed on the next strongest pairs of coded spatial-subspace channels. Once all of the coded receive-weighted data symbols are detected, the receive-weighted uncoded data symbols on the uncoded spatial-subspace channels are then processed as described previously. Alternatively, a form of

20 coding may be used in which there are more than two coded spatial-subspace channels which are dependent on one another. In any of the cases where there is more than two coded spatial-subspace channels, the iterative decoding/detection scheme comprises processing data transmitted on at least a portion of the coded spatial-subspace channels in the first step of each

25 iteration.

**[00132]** Referring now to Figure 9, shown therein is a block diagram of the data estimation unit 238 that performs the iterative decoding/detection process. The data estimation unit 238 comprises a subspace matrix unit 300 and a symbol matrix unit 302. The subspace matrix unit 300 is connected to

30 the receiver link adaptation unit 242 to receive the initial singular value matrix  $\Lambda_k$  and updates of the quasi-diagonal singular value matrix  $\Lambda_{ek}$  (see equation

9). The symbol matrix unit **302** is connected to the receiver weighting unit **234** (via the multiplexer **MUX2**) to receive the receive-weighted spatial-subspace data and store this data in the receive-weighted data symbol matrix  $r_k$ .

**[00133]** The data estimation unit **238** further comprises a coefficient calculator **304**, a calculation unit **306** and a first power weighting unit **308**. The coefficient calculator **304** calculates the various weighting coefficients required by the iterative detection/decoding process. Accordingly, the coefficient calculator **304** is connected to the receiver link adaptation unit **242** to receive the adaptive power allocation coefficients  $\alpha_i$  from which the inverse power coefficients  $\beta_i$  are calculated. The coefficient calculator **304** is also connected to the subspace matrix unit **300** to receive various components of the quasi-diagonal singular value matrix  $\Lambda_{ek}$  for calculating the coefficients  $\gamma$  and  $\delta$  (see equations 13 and 16).

**[00134]** The calculation unit **306** calculates the estimated receive-weighted uncoded and coded data symbols in the received symbol matrix  $r_k$  in accordance with equations 11 to 16. Accordingly, the calculation unit **306** is connected to the coefficient calculator **304** to receive the coefficients  $\gamma$  and  $\delta$ . The calculation unit **306** is also connected to the receiver link adaptation unit **242** to receive the spatial-subspace channel coding transmission parameter for determining whether the spatial-subspace channels for the sub-carrier **k** are uncoded, coded or a combination of coded and uncoded. As mentioned previously, if a combination of coded and uncoded spatial-subspace channels are transmitted on the sub-carrier **k**, then the calculation unit **306** performs calculations in accordance with equations 11 to 16 for calculating the estimated receive-weighted uncoded and coded data symbols. Alternatively, if only coded spatial-subspace channels were transmitted on the sub-carrier **k**, then the calculation unit **306** performs calculations in accordance with equations 11 to 13 for calculating the estimated receive-weighted coded data symbols. In another alternative, if only uncoded spatial-subspace channels are transmitted on the sub-carrier **k**, then the calculation unit **306** performs



- 56 -

calculations in accordance with equations 14 to 16 for calculating the estimated receive-weighted uncoded data symbols.

[00135] The first power weighting unit 308 is connected to the calculation unit 306 to receive the estimated receive-weighted coded and  
5 uncoded data symbols and weight these estimated data symbols with the weights  $\beta_i$ . The weights  $\beta_i$  are the inverse of the adaptive power allocation coefficients  $\alpha_i$  that were used by the power allocation unit 134 of the transmitter 112. The output of the first power weighting unit 308 are power-weighted estimated uncoded and coded data symbols.

10 [00136] A detection unit 310, connected to the first power weighting unit 308, receives the power-weighted estimated uncoded and coded data symbols and applies a detection method to these data symbols. The detection unit 310 preferably applies the maximum likelihood method to these data  
15 symbols for producing detected coded data symbols and detected uncoded data symbols. Accordingly, the detection unit 310 is connected to the receiver link adaptation unit 242 to receive the spatial-subspace channel modulation transmission parameter for the sub-carrier k. This parameter specifies the modulation scheme and modulation rate that was used to create these data  
20 symbols at the transmitter 112. The detection unit 310 produces the detected symbols by comparing the power-weighted estimated uncoded and coded data symbols with the symbols of the constellation associated with the modulation scheme to find the closest data symbol in the constellation.

[00137] The data estimation unit 238 further comprises a second power weighting unit 312 and a recoding unit 314 that are connected between the  
25 detection unit 310 and the symbol matrix unit 302. The locations of the weighting unit 312 and the recoding unit 314 are interchangeable. The weighting unit 312 and the recoding unit 314 process the detected uncoded and coded data symbols by weighting these symbols with the adaptive power allocation coefficients  $\alpha_i$  and coding these symbols in accordance with the  
30 spatial-subspace channel coding transmission parameter. Accordingly, the second power weighting unit 312 is connected to the coefficient calculator 304

- 57 -

to receive the adaptive power allocation coefficients  $\alpha_i$  and the recoding unit 314 is connected to the receiver link adaptation unit 242 to receive the channel coding transmission parameter. The processed data is then provided to the symbol matrix unit 302 to be entered within the receive-weighted data symbol matrix  $r_k$  so that the data estimation unit 238 may perform another iteration of the iterative decoding/detection process.

[00138] The data estimation unit 238 further comprises a de-mapper unit 316 which applies a de-mapping process to the power-weighted estimated uncoded and coded data symbols for obtaining output data. Accordingly, the de-mapper unit 316 is connected to the first power weighting unit 308 to receive the power-weighted estimated uncoded and coded symbols. The de-mapper unit 316 is also connected to the receiver link adaptation unit 242 to receive the spatial-subspace channel modulation transmission parameter so that the de-mapper unit 316 can apply the appropriate constellation during the de-mapping process. The de-mapper unit 316 may utilize a hard or soft decision algorithm in this de-mapping process, as is well known to those skilled in the art. If a hard-decision process is used, then the output data from the de-mapper unit 316 comprises the output data bit stream  $y_b$ . If a soft decision process is used, then the output data from the de-mapper unit 316 comprises output data symbols with corresponding confidence levels. The power-weighted estimated uncoded and coded data symbols are provided to the de-mapper unit 316 after the data estimation unit 238 has performed a desired number of iterations of the iterative decoding/detection process.

[00139] One or more digital signal processor (DSPs), general purpose programmable processors, application specific circuitry and/or FPGAs may be used to implement the various units of the transmitters 12 and 112 and receivers 16 and 216 described herein. In addition, onboard or external ROM, flash EEPROM, or ferroelectric RAM may also be used. In addition, as previously mentioned, the transmitters 12 and 112 and the receivers 16 and 216 described herein actually function as transceivers. These transceivers

- 58 -

incorporate the structure of both the transmitter and the receiver with the transmitter and receiver being connected via the data pump.

**[00140]** Various types of coding and error correction can be utilized for the various types of information transmitted by the communication system of  
5 the present invention. For instance, turbo product code, as is well known by those skilled in the art, may be used for forward error correction for the data bits **xb** prior to conversion to data symbols with a selected code rate and generator polynomial. CRC bits could also be included in the data bits **xb**. Forward error correction can also be applied to the channel/transmission  
10 information data.

**[00141]** Although the preceding detailed discussion contains many specifics for the purposes of illustration, anyone of ordinary skill in the art will appreciate that the description is not to be considered as limiting the scope of the present invention, but rather as merely providing a particular preferred  
15 working embodiment thereof. For instance, the communication system is not restricted to OFDM-based systems and can be used for any communication system that employs multiple antennas at the transmitter and receiver and transmits data on at least one sub-carrier. Furthermore, the communication system is not restricted to wireless contexts and may exploit any channel  
20 having multiple inputs or multiple outputs and certain other characteristics. Accordingly, one skilled in the art will appreciate that many variations and alterations can be made to the embodiment described and illustrated herein, without departing from the present invention, the scope of which is defined in the appended claims.

**Claims:**

1. A communication system for transmitting an input data symbol stream over a plurality of spatial-subspace channels of a sub-carrier between a transmitter and a receiver, wherein said transmitter comprises:

- 5                   a) an encoder unit for processing a plurality of input data symbol sub-streams for providing a plurality of uncoded/coded input data symbol sub-streams comprising at least one of: 1) at least one uncoded input data symbol sub-stream for allocation on a corresponding at least one uncoded spatial-subspace channel of said plurality of spatial-subspace channels and 2) at  
10                   least two coded input data symbol sub-streams for allocation on a corresponding at least two coded spatial-subspace channels of said plurality of spatial-subspace channels, said plurality of input data symbol sub-streams being derived from said input  
15                   data symbol stream;
- b) a transmitter weighting unit connected to said encoder unit for weighting said plurality of uncoded/coded input data symbol sub-streams with a transmit weight matrix corresponding to said sub-carrier for distributing said plurality of uncoded/coded input  
20                   data symbol sub-streams along said plurality of spatial-subspace channels and providing transmit-weighted spatial-subspace data;

wherein, said receiver comprises:

- 25                   c) a receiver weighting unit for receiving spatial-subspace data related to said transmit-weighted spatial-subspace data and weighting said spatial-subspace data with a receive weight matrix for providing receive-weighted spatial-subspace data; and,
- 30                   d) a data estimation unit connected to said receiver weighting unit for receiving and performing an iterative processing method on said receive-weighted spatial-subspace data to estimate

- 60 -

output data related to said input data symbol stream, said iterative processing method comprising successively processing data on each of said plurality of spatial-subspace channels in said receive-weighted spatial-subspace data.

- 5 2. The communication system of claim 1, wherein said plurality of spatial-subspace channels comprise only uncoded spatial-subspace channels and said data estimation unit is adapted to perform a successive interference cancellation method for providing said estimated output data by detecting  
10 channels, subtracting detected receive-weighted data symbols from the receive-weighted spatial-subspace data and iteratively processing receive-weighted spatial-subspace data on remaining uncoded spatial-subspace channels in a similar fashion.
3. The communication system of claim 2, wherein the uncoded spatial-  
15 subspace channels are processed in order of decreasing signal to noise plus interference ratio.
4. The communication system of claim 1, wherein said plurality of spatial-subspace channels comprise only said at least two coded spatial-subspace channels and said data estimation unit is adapted to perform an iterative  
20 decoding/detection method on the receive-weighted spatial-subspace data for providing said estimated output data, with one iteration of said decoding/detection method comprising: (1) decoding and detecting receive-weighted coded data symbols transmitted on at least a portion of said at least  
25 two coded spatial-subspace channels and replacing said receive-weighted coded data symbols in said receive-weighted spatial-subspace data with detected coded data symbols; and, (2) processing receive-weighted spatial-subspace data on remaining coded spatial-subspace channels in a similar fashion.

- 61 -

5. The communication system of claim 4, wherein said at least two coded spatial-subspace channels comprise pairs of coded spatial-subspace channels which are processed in order of decreasing signal to noise plus interference ratio.

5 6. The communication system of claim 1, wherein said plurality of spatial-subspace channels comprise said at least two coded spatial-subspace channels and said at least one uncoded spatial-subspace channel and said data estimation unit is adapted to perform an iterative decoding/detection method on the receive-weighted spatial-subspace data for providing said  
10 estimated output data, with one iteration of said decoding/detection method comprising: (1) decoding and detecting receive-weighted coded data symbols transmitted on at least a portion of said at least two coded spatial-subspace channels and replacing said receive-weighted coded data symbols in said receive-weighted spatial-subspace data with detected coded data symbols;  
15 and, (2) estimating and detecting uncoded data symbols transmitted on said at least one uncoded spatial-subspace channel.

7. The communication system of claim 6, wherein said at least two coded spatial-subspace channels comprise pairs of coded spatial-subspace channels which are processed in step (1) in order of decreasing signal to  
20 noise plus interference ratio, and said at least one uncoded spatial-subspace channel is processed in step (2) in order of decreasing signal to noise plus interference ratio.

8. The communication system of claim 1, wherein said data estimation unit comprises a de-mapper unit that utilizes one of: 1) a hard-decision  
25 method on detected data for providing output data bits as said estimated output data, and 2) a soft-decision method on detected data for providing output data symbols with associated confidence levels as said estimated output data.

- 62 -

9. The communication system of claim 1, wherein said transmitter further comprises a first data mapper unit for mapping an input data bit stream to said input data symbol stream according to a modulation scheme having a constellation, and a subspace allocation unit for converting said input data  
5 symbol stream into said plurality of input data symbol sub-streams for allocation over said plurality of spatial-subspace channels, said first data mapper being connected to said subspace allocation unit, wherein said subspace allocation unit and said first data mapper unit operate in unison for implementing a multi-resolution modulation scheme wherein input data  
10 symbols which are further apart from one another in said constellation are allocated to one of said plurality of input data symbol sub-streams associated with one of said plurality of spatial-subspace channels having a low signal-to-noise-plus-interference ratio with respect to said plurality of spatial-subspace channels.
- 15 10. The communication system of claim 9, wherein input data symbols which are closer to one another in said constellation are allocated to one of said plurality of input data symbol sub-streams associated with one of said plurality of spatial-subspace channels having a high signal-to-noise-plus-interference ratio with respect to said plurality of spatial-subspace channels.
- 20 11. A method for transmitting an input data symbol stream over a plurality of spatial-subspace channels of a sub-carrier between a transmitter and a receiver, wherein at the transmitter the method comprises:
- 25 a) processing a plurality of input data symbol sub-streams for providing a plurality of uncoded/coded input data symbol sub-streams comprising at least one of: 1) at least one uncoded input data symbol sub-stream for allocation on a corresponding at least one uncoded spatial-subspace channel of said plurality of spatial-subspace channels and 2) at least two coded input data symbol sub-streams for allocation on a corresponding at  
30 least two coded spatial-subspace channels of said plurality of

- 63 -

spatial-subspace channels, said plurality of input data symbol sub-streams being derived from said input data symbol stream;

- 5           b) weighting said plurality of uncoded/coded input data symbol sub-streams with a transmit weight matrix corresponding to said sub-carrier for distributing said plurality of uncoded/coded input data symbol sub-streams along said plurality of spatial-subspace channels and providing transmit-weighted spatial-subspace data;

wherein, at the receiver the method further comprises:

- 10           c) receiving spatial-subspace data related to said transmit-weighted spatial-subspace data and weighting said spatial-subspace data with a receive weight matrix for providing receive-weighted spatial-subspace data; and,
- 15           d) performing an iterative processing method on said receive-weighted spatial-subspace data to estimate output data related to said input data symbol stream, said iterative processing method comprising successively processing data on each of said plurality of spatial-subspace channels in said receive-weighted spatial-subspace data.

- 20   12.   The method of claim 11, wherein said plurality of spatial-subspace channels comprise only uncoded spatial-subspace channels and step (d) comprises performing a successive interference cancellation method for providing said estimated output data by detecting receive-weighted data symbols on one of said uncoded spatial-subspace channels, subtracting
- 25   detected receive-weighted data symbols from the receive-weighted spatial-subspace data and iteratively processing receive-weighted spatial-subspace data on remaining uncoded spatial-subspace channels in a similar fashion.

13.   The method of claim 12, wherein step (d) further comprises processing the uncoded spatial-subspace channels in order of decreasing signal to noise
- 30   plus interference ratio.



- 64 -

14. The method of claim 11, wherein said plurality of spatial-subspace channels comprise only said at least two coded spatial-subspace channels and step (d) comprises performing an iterative decoding/detection method on the receive-weighted spatial-subspace data for providing said estimated  
5 output data, with one iteration of said decoding/detection method comprising: (1) decoding and detecting receive-weighted coded data symbols transmitted on at least a portion of said at least two spatial-subspace channels and replacing said receive-weighted coded data symbols in said receive-weighted spatial-subspace data with detected coded data symbols; and, (2) processing  
10 receive-weighted spatial-subspace data on remaining coded spatial-subspace channels in a similar fashion.

15. The method of claim 14, wherein said at least two coded spatial-subspace channels comprise pairs of coded spatial-subspace channels and step (d) further comprises processing said pairs of coded spatial-subspace  
15 channels in order of decreasing signal to noise plus interference ratio.

16. The method of claim 11, wherein said plurality of spatial-subspace channels comprise said at least two coded spatial-subspace channels and said at least one uncoded spatial-subspace channel and step (d) comprises performing an iterative decoding/detection method on the receive-weighted  
20 spatial-subspace data for providing said estimated output data, with one iteration of said decoding/detection method comprising: (1) decoding and detecting receive-weighted coded data symbols transmitted on at least a portion of said at least two coded spatial-subspace channels and replacing said receive-weighted coded data symbols in said receive-weighted spatial-  
25 subspace data with detected coded data symbols; and, (2) estimating and detecting uncoded data symbols transmitted on said at least one uncoded spatial-subspace channel.

17. The method of claim 16, wherein said at least two coded spatial-subspace channels comprise pairs of coded spatial-subspace channels and  
30 step (d) further comprises processing said pairs of coded spatial-subspace

- 65 -

channels in step (1) in order of decreasing signal to noise plus interference ratio, and processing said at least one uncoded spatial-subspace channel in step (2) in order of decreasing signal to noise plus interference ratio.

18. The method of claim 11, wherein step (d) further comprises applying one of: 1) a hard-decision method on detected data for providing output data bits as said estimated output data, and 2) a soft-decision method on detected data for providing output data symbols with associated confidence levels as said estimated output data.

19. The method of claim 11, wherein said method further comprises mapping an input data bit stream to said input data symbol stream according to a modulation scheme having a constellation and converting said input data symbol stream into said plurality of input data symbol sub-streams for allocation over said plurality of spatial-subspace channels, wherein said converting and said mapping is done in unison for implementing a multi-resolution modulation scheme wherein input data symbols which are further apart from one another in said constellation are allocated to one of said plurality of input data symbol sub-streams associated with one of said plurality of spatial-subspace channels having a low signal-to-noise-plus-interference ratio with respect to said plurality of spatial-subspace channels.

20. The method of claim 19, wherein input data symbols which are closer to one another in said constellation are allocated to one of said plurality of input data symbol sub-streams associated with one of said plurality of spatial-subspace channels having a high signal-to-noise-plus-interference ratio with respect to said plurality of spatial-subspace channels.

21. A receiver for receiving spatial-subspace data transmitted over a plurality of spatial-subspace channels of a sub-carrier, said spatial-subspace data comprising a plurality of uncoded/coded data symbol sub-streams comprising at least one of: 1) at least one uncoded input data symbol sub-stream for allocation on a corresponding at least one uncoded spatial-

- 66 -

subspace channel of said plurality of spatial-subspace channels and 2) at least two coded input data symbol sub-streams for allocation on a corresponding at least two coded spatial-subspace channels of said plurality of spatial-subspace channels, wherein said receiver comprises:

- 5                   a) a receiver weighting unit for weighting said spatial-subspace data with a receive weight matrix for providing receive-weighted spatial-subspace data; and,
- b) a data estimation unit connected to said receiver weighting unit for receiving and performing an iterative processing method
- 10                   on said receive-weighted spatial-subspace data to estimate output data related to said input data symbol stream, said iterative processing method comprising successively processing data on each of said plurality of spatial-subspace channels in said receive-weighted spatial-subspace data.

15   22.   The receiver of claim 21, wherein said plurality of spatial-subspace channels comprise only uncoded spatial-subspace channels and said data estimation unit is adapted to perform a successive interference cancellation method for providing said estimated output data by detecting receive-weighted data symbols on one of said uncoded spatial-subspace channels,

20   subtracting detected receive-weighted data symbols from the receive-weighted spatial-subspace data and iteratively processing receive-weighted spatial-subspace data on remaining uncoded spatial-subspace channels in a similar fashion.

23.   The receiver of claim 21, wherein said plurality of spatial-subspace

25   channels comprise only said at least two coded spatial-subspace channels and said data estimation unit is adapted to perform an iterative decoding/detection method on the receive-weighted spatial-subspace data for providing said estimated output data, with one iteration of said decoding/detection method comprising: (1) decoding and detecting receive-

30   weighted coded data symbols transmitted on at least a portion said at least two coded spatial-subspace channels and replacing said receive-weighted

- 67 -

coded data symbols in said receive-weighted spatial-subspace data with detected coded data symbols; and, (2) processing receive-weighted spatial-subspace data on remaining coded spatial-subspace channels in a similar fashion.

5 24. The receiver of claim 21, wherein said plurality of spatial-subspace channels comprise said at least two coded spatial-subspace channels and said at least one uncoded spatial-subspace channel and said data estimation unit is adapted to perform an iterative decoding/detection method on the receive-weighted spatial-subspace data for providing said estimated output  
10 data, with one iteration of said decoding/detection method comprising: (1) decoding and detecting receive-weighted coded data symbols transmitted on at least a portion of said at least two coded spatial-subspace channels and replacing said receive-weighted coded data symbols in said receive-weighted spatial-subspace data with detected coded data symbols; and, (2) estimating  
15 and detecting uncoded data symbols transmitted on said at least one uncoded spatial-subspace channel.

25. The receiver of claim 21, wherein said data estimation unit comprises a de-mapper unit that utilizes one of: 1) a hard-decision method on detected data for providing output data bits as said estimated output data, and 2) a  
20 soft-decision method on detected data for providing output data symbols with associated confidence levels as said estimated output data.

26. A method for receiving spatial-subspace data transmitted over a plurality of spatial-subspace channels of a sub-carrier, said spatial-subspace data comprising a plurality of uncoded/coded data symbol sub-streams  
25 comprising at least one of: 1) at least one uncoded input data symbol sub-stream for allocation on a corresponding at least one uncoded spatial-subspace channel of said plurality of spatial-subspace channels and 2) at least two coded input data symbol sub-streams for allocation on a corresponding at least two coded spatial-subspace channels of said plurality  
30 of spatial-subspace channels, wherein said method comprises:

- 68 -

a) weighting said spatial-subspace data with a receive weight matrix for providing receive-weighted spatial-subspace data; and,

5 b) performing an iterative processing method on said receive-weighted spatial-subspace data to estimate output data related to said input data symbol stream, said iterative processing method comprising successively processing data on each of said plurality of spatial-subspace channels in said receive-weighted spatial-subspace data.

10 27. The method of claim 26, wherein said plurality of spatial-subspace channels comprise only uncoded spatial-subspace channels and step (b) comprises performing a successive interference cancellation method for providing said estimated output data by detecting receive-weighted data symbols on one of said uncoded spatial-subspace channels, subtracting  
15 detected receive-weighted data symbols from the receive-weighted spatial-subspace data and iteratively processing receive-weighted spatial-subspace data on remaining uncoded spatial-subspace channels in a similar fashion.

28. The method of claim 26, wherein said plurality of spatial-subspace channels comprise only said at least two coded spatial-subspace channels  
20 and step (b) comprises performing an iterative decoding/detection method on the receive-weighted spatial-subspace data for providing said estimated output data, with one iteration of said decoding/detection method comprising: (1) decoding and detecting receive-weighted coded data symbols transmitted on at least a portion of said at least two spatial-subspace channels and  
25 replacing said receive-weighted coded data symbols in said receive-weighted spatial-subspace data with detected coded data symbols; and, (2) processing receive-weighted spatial-subspace data on remaining coded spatial-subspace channels in a similar fashion.

29. The method of claim 26, wherein said plurality of spatial-subspace  
30 channels comprise said at least two coded spatial-subspace channels and

- 69 -

said at least one uncoded spatial-subspace channel and step (b) comprises performing an iterative decoding/detection method on the receive-weighted spatial-subspace data for providing said estimated output data, with one iteration of said decoding/detection method comprising: (1) decoding and  
5 detecting receive-weighted coded data symbols transmitted on at least a portion of said at least two coded spatial-subspace channels and replacing said receive-weighted coded data symbols in said receive-weighted spatial-subspace data with detected coded data symbols; and, (2) estimating and detecting uncoded data symbols transmitted on said at least one uncoded  
10 spatial-subspace channel.

30. The method of claim 26, wherein step (d) further comprises applying one of: 1) a hard-decision method on detected data for providing output data bits as said estimated output data, and 2) a soft-decision method on detected data for providing output data symbols with associated confidence levels as  
15 said estimated output data.

31. A communication system for transmitting input data over a plurality of spatial-subspace channels of a sub-carrier between a transmitter and a receiver, wherein said transmitter comprises:

a) an encoder unit for processing a plurality of input data  
20 symbol sub-streams for providing a plurality of uncoded/coded input data symbol sub-streams comprising at least one of: 1) at least one uncoded input data symbol sub-stream for allocation on a corresponding at least one uncoded spatial-subspace channel of said plurality of spatial-subspace channels and 2) at  
25 least two coded input data symbol sub-streams for allocation on a corresponding at least two coded spatial-subspace channels of said plurality of spatial-subspace channels, said transmitter transmitting data related to said plurality of uncoded/coded input data symbol sub-streams; and,

30 wherein, said receiver comprises:

- 70 -

5                   b) a data estimation unit for performing an iterative processing method on received spatial-subspace data to estimate output data related to said input data, said iterative processing method comprising successively processing data on each of said plurality of spatial-subspace channels in said received spatial-subspace data.

32.   The communication system of claim 31, wherein said plurality of spatial-subspace channels comprise only uncoded spatial-subspace channels and said data estimation unit is adapted to perform a successive interference  
10   cancellation method for providing said estimated output data by detecting received data symbols on one of said uncoded spatial-subspace channels, subtracting detected received data symbols from the received spatial-subspace data and iteratively processing received spatial-subspace data on remaining uncoded spatial-subspace channels in a similar fashion.

15   33.   The communication system of claim 31, wherein said plurality of spatial-subspace channels comprise only said at least two coded spatial-subspace channels and said data estimation unit is adapted to perform an iterative decoding/detection method on the received spatial-subspace data for providing said estimated output data, with one iteration of said  
20   decoding/detection method comprising: (1) decoding and detecting received coded data symbols transmitted on at least a portion of said at least two coded spatial-subspace channels and replacing said received coded data symbols in said received spatial-subspace data with detected coded data symbols; and, (2) processing received spatial-subspace data on remaining  
25   coded spatial-subspace channels in a similar fashion.

34.   The communication system of claim 31, wherein said plurality of spatial-subspace channels comprise said at least two coded spatial-subspace channels and said at least one uncoded spatial-subspace channel and said data estimation unit is adapted to perform an iterative decoding/detection  
30   method on the received spatial-subspace data for providing said estimated

- 71 -

output data, with one iteration of said decoding/detection method comprising:  
(1) decoding and detecting received coded data symbols transmitted on at  
least a portion of said at least two coded spatial-subspace channels and  
replacing said received coded data symbols in said received spatial-subspace  
5 data with detected coded data symbols; and, (2) estimating and detecting  
uncoded data symbols transmitted on said at least one uncoded spatial-  
subspace channel.

35. The communication system of claim 31, wherein said transmitter  
further comprises a first data mapper unit for mapping an input data bit stream  
10 to an input data symbol stream according to a modulation scheme having a  
constellation, and a subspace allocation unit for converting said input data  
symbol stream into said plurality of input data symbol sub-streams for  
allocation over said plurality of spatial-subspace channels, said first data  
mapper being connected to said subspace allocation unit, wherein said  
15 subspace allocation unit and said first data mapper unit operate in unison for  
implementing a multi-resolution modulation scheme wherein input data  
symbols which are further apart from one another in said constellation are  
allocated to one of said plurality of input data symbol sub-streams associated  
with one of said plurality of spatial-subspace channels having a low signal-to-  
20 noise-plus-interference ratio with respect to said plurality of spatial-subspace  
channels.

36. The communication system of claim 35, wherein input data symbols  
which are closer to one another in said constellation are allocated to one of  
said plurality of input data symbol sub-streams associated with one of said  
25 plurality of spatial-subspace channels having a high signal-to-noise-plus-  
interference ratio with respect to said plurality of spatial-subspace channels.

37. A method for transmitting input data over a plurality of spatial-subspace  
channels of a sub-carrier between a transmitter and a receiver, wherein at the  
transmitter the method comprises:



- 72 -

5 a) processing a plurality of input data symbol sub-streams for providing a plurality of uncoded/coded input data symbol sub-streams comprising at least one of: 1) at least one uncoded input data symbol sub-stream for allocation on a corresponding at least one uncoded spatial-subspace channel of said plurality of spatial-subspace channels and 2) at least two coded input data symbol sub-streams for allocation on a corresponding at least two coded spatial-subspace channels of said plurality of spatial-subspace channels, and transmitting data related to said plurality of uncoded/coded input data symbol sub-streams; and, 10 wherein, at the receiver the method further comprises:

15 b) performing an iterative processing method on received spatial-subspace data to estimate output data related to said input data, said iterative processing method comprising successively processing data on each of said plurality of spatial-subspace channels in said received spatial-subspace data.

38. The method of claim 37, wherein said plurality of spatial-subspace channels comprise only uncoded spatial-subspace channels and step (b) comprises performing a successive interference cancellation method for 20 providing said estimated output data by detecting received data symbols on one of said uncoded spatial-subspace channels, subtracting detected received data symbols from the received spatial-subspace data and iteratively processing received spatial-subspace data on remaining uncoded spatial-subspace channels in a similar fashion.

25 39. The method of claim 37, wherein said plurality of spatial-subspace channels comprise only said at least two coded spatial-subspace channels and step (b) comprises performing an iterative decoding/detection method on the received spatial-subspace data for providing said estimated output data, with one iteration of said decoding/detection method comprising: (1) decoding 30 and detecting received coded data symbols transmitted on at least a portion

of said at least two spatial-subspace channels and replacing said received coded data symbols in said received spatial-subspace data with detected coded data symbols; and, (2) processing received spatial-subspace data on remaining coded spatial-subspace channels in a similar fashion.

- 5 40. The method of claim 37, wherein said plurality of spatial-subspace channels comprise said at least two coded spatial-subspace channels and said at least one uncoded spatial-subspace channel and step (b) comprises performing an iterative decoding/detection method on the received spatial-subspace data for providing said estimated output data, with one iteration of  
10 said decoding/detection method comprising: (1) decoding and detecting received coded data symbols transmitted on at least a portion of said at least two coded spatial-subspace channels and replacing said received coded data symbols in said received spatial-subspace data with detected coded data symbols; and, (2) estimating and detecting uncoded data symbols transmitted  
15 on said at least one uncoded spatial-subspace channel.

41. The method of claim 37, wherein said method further comprises mapping an input data bit stream to an input data symbol stream according to a modulation scheme having a constellation and converting said input data symbol stream into said plurality of input data symbol sub-streams for  
20 allocation over said plurality of spatial-subspace channels, wherein said converting and said mapping is done in unison for implementing a multi-resolution modulation scheme wherein input data symbols which are further apart from one another in said constellation are allocated to one of said plurality of input data symbol sub-streams associated with one of said plurality  
25 of spatial-subspace channels having a low signal-to-noise-plus-interference ratio with respect to said plurality of spatial-subspace channels.

42. The method of claim 41, wherein input data symbols which are closer to one another in said constellation are allocated to one of said plurality of input data symbol sub-streams associated with one of said plurality of spatial-

- 74 -

subspace channels having a high signal-to-noise-plus-interference ratio with respect to said plurality of spatial-subspace channels.

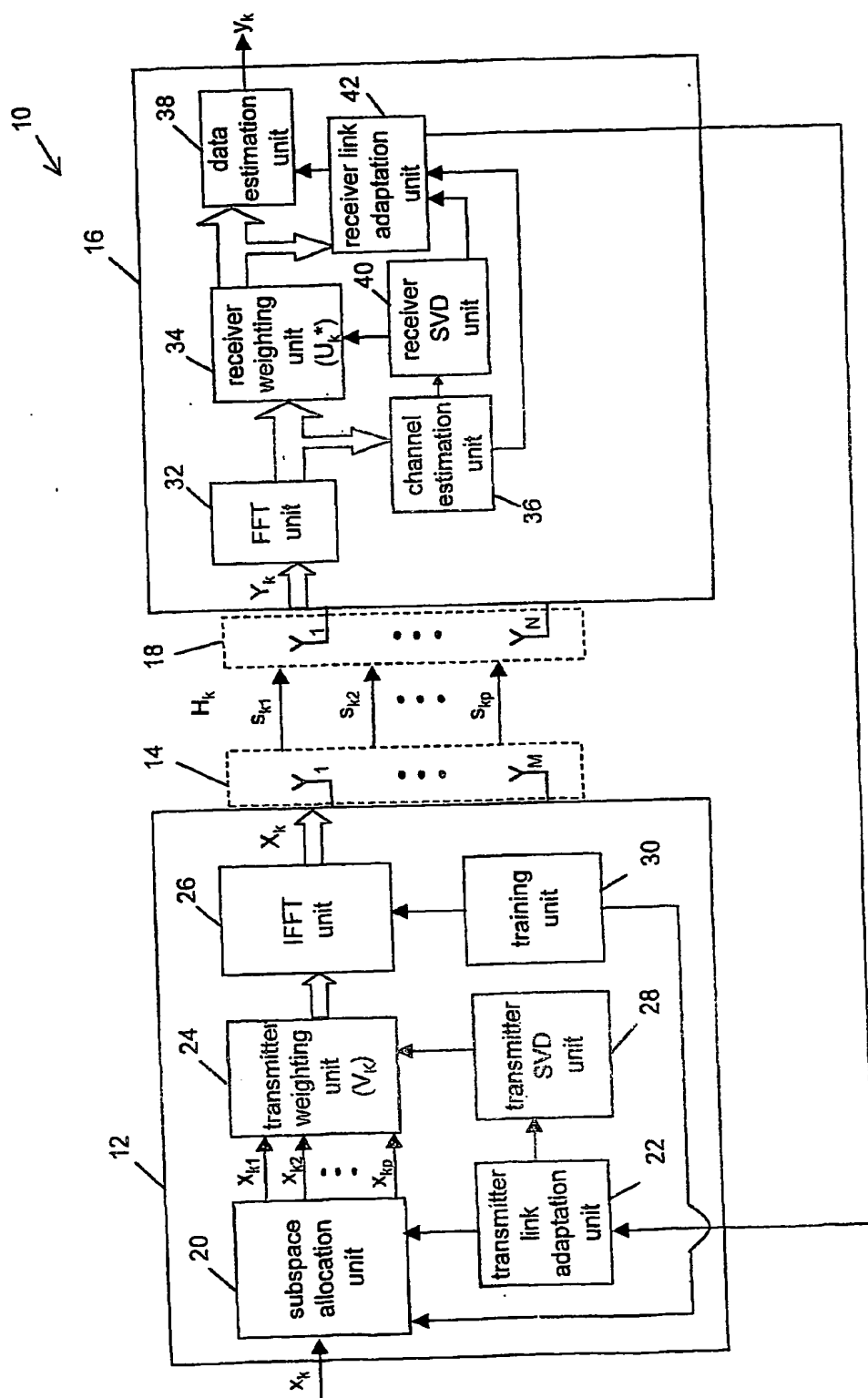


Figure 1

2/9

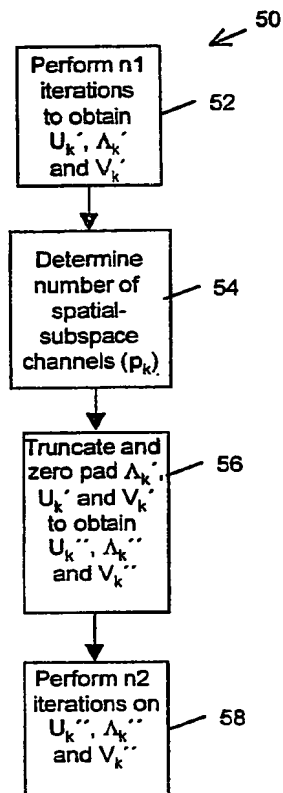


FIGURE 2

frequency

$$H_1 = \begin{bmatrix} H_1(1,1) & \cdots & H_1(1,N) \\ \vdots & & \vdots \\ H_1(M,1) & \cdots & H_1(M,N) \end{bmatrix}$$

$$H_{1\max} = \begin{bmatrix} H_{1\max}(1,1) & \cdots & H_{1\max}(1,N) \\ \vdots & & \vdots \\ H_{1\max}(M,1) & \cdots & H_{1\max}(M,N) \end{bmatrix}$$

60

FIGURE 3a

time

$$h_1 = \begin{bmatrix} h_1(1,1) & \cdots & h_1(1,N) \\ \vdots & & \vdots \\ h_1(M,1) & \cdots & h_1(M,N) \end{bmatrix}$$

$$h_{1\max} = \begin{bmatrix} h_{1\max}(1,1) & \cdots & h_{1\max}(1,N) \\ \vdots & & \vdots \\ h_{1\max}(M,1) & \cdots & h_{1\max}(M,N) \end{bmatrix}$$

62

FIGURE 3b

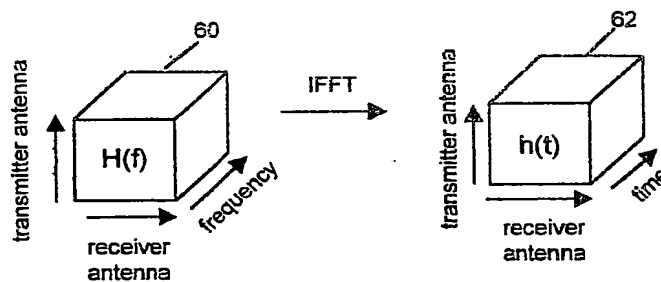


FIGURE 3c

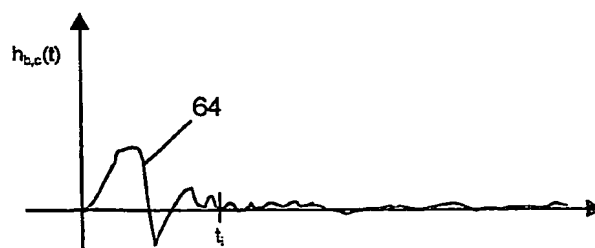


FIGURE 3d

3/9

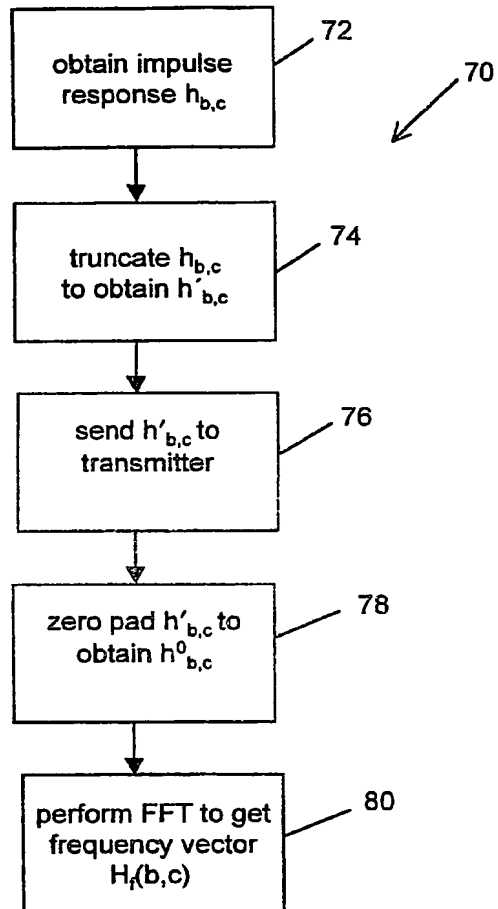


FIGURE 4

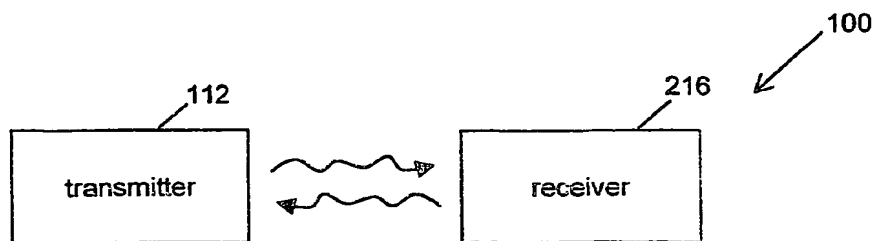


FIGURE 5a

4/9

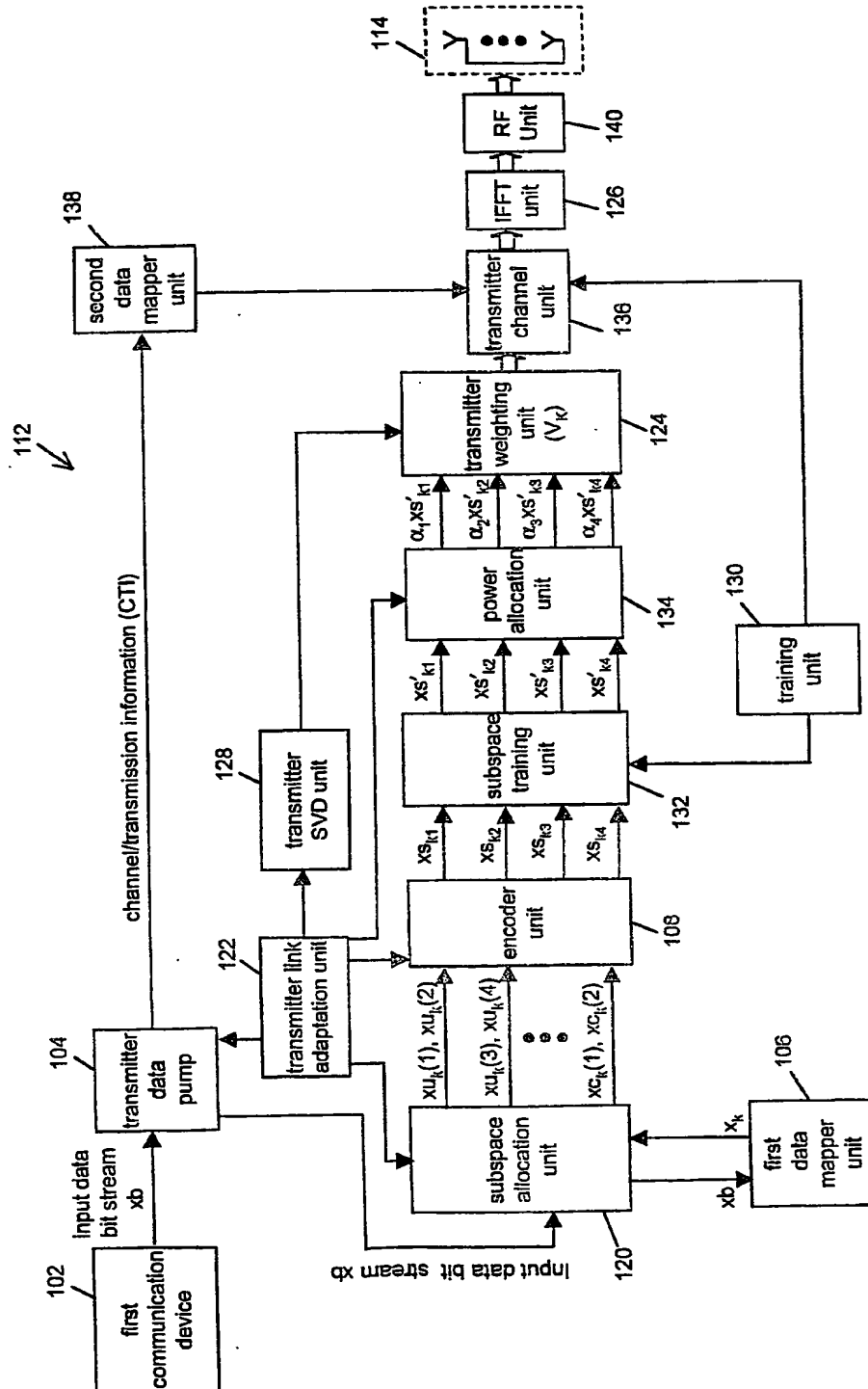


Figure 5b

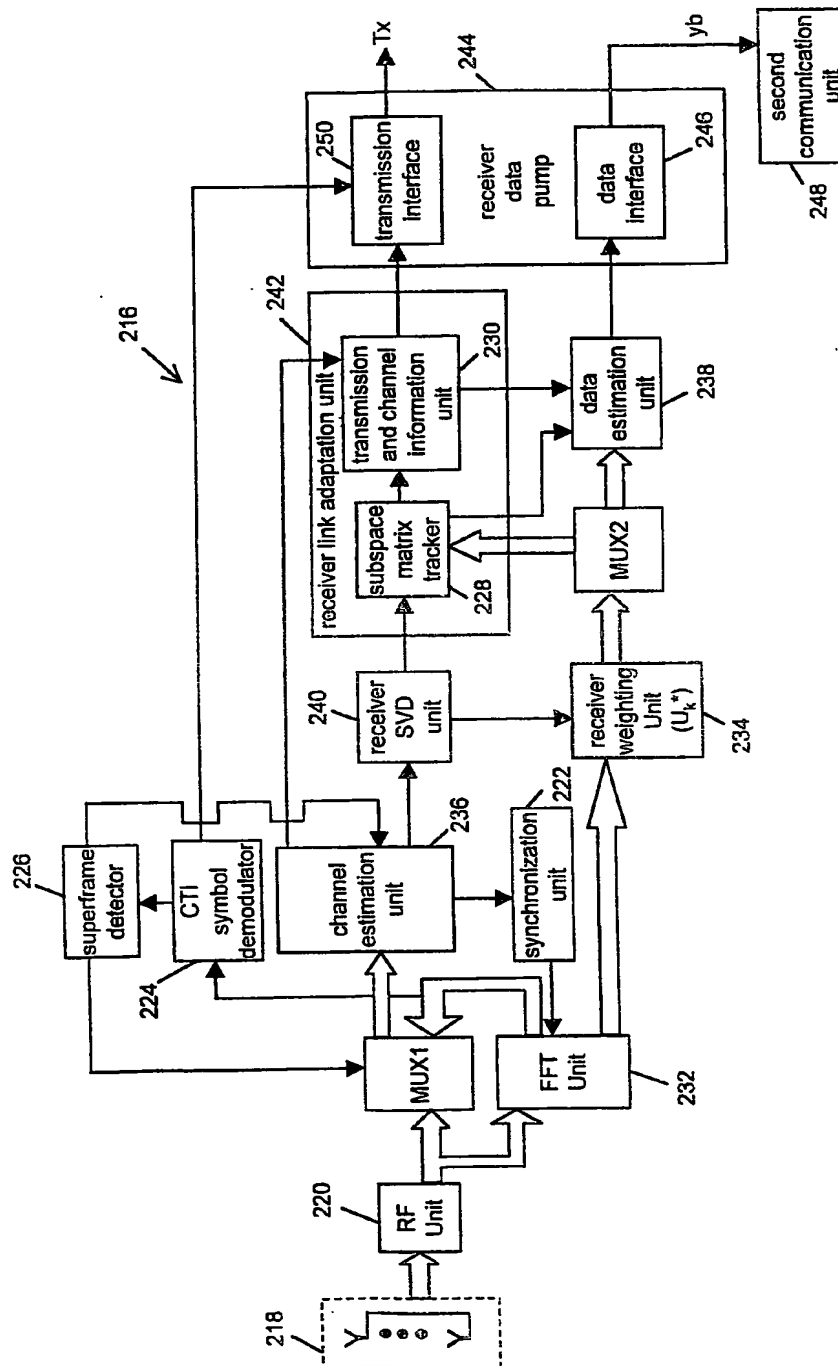


Figure 5c



6/9

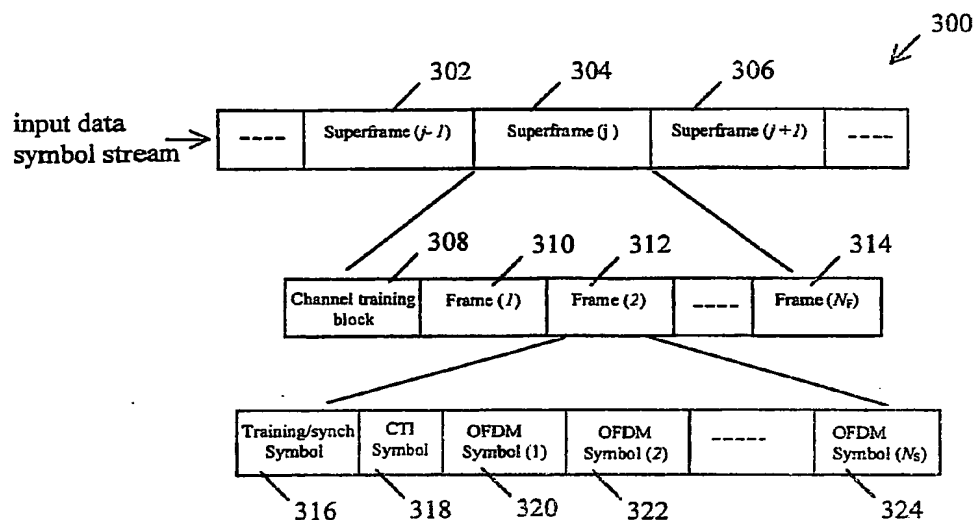


Figure 6a

TX	OFDM Symbol number at the beginning of a superframe											
	1	2	3	4	5	6	7	8	29	30	31	32
1	HT	HT	HT	HT	HT	HT	HT	HT				
2					HT	HT	HT	HT				
3												
4												
5												
6												
7												
8									HT	HT	HT	HT

Figure 6b

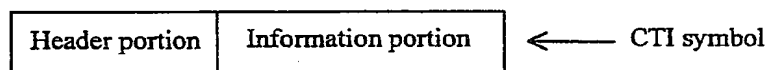


Figure 6c

TX	OFDM Frame number											
	12f+1	12f+2	12f+3	12f+4	12f+5	12f+6	12f+7	12f+8	12f+9	12f+10	12f+11	12f+12
1		SY										
2			SY									
3					SY							
4						SY						
5							SY					
6								SY				
7									SY			
8											SY	

Figure 6d

7/9

Subspace	OFDM Frame number											
	12H+1	12H+2	12H+3	12H+4	12H+5	12H+6	12H+7	12H+8	12H+9	12H+10	12H+11	12H+12
$S_{k1}$	$\Delta T_1$											
$S_{k2}$				$\Delta T_2$								
$S_{k3}$							$\Delta T_3$					
$S_{k4}$										$\Delta T_4$		

Figure 7a

TX	OFDM Frame number											
	12H+1	12H+2	12H+3	12H+4	12H+5	12H+6	12H+7	12H+8	12H+9	12H+10	12H+11	12H+12
1	$\Delta T_1$			$\Delta T_2$			$\Delta T_3$			$\Delta T_4$		
2	$\Delta T_1$			$\Delta T_2$			$\Delta T_3$			$\Delta T_4$		
3	$\Delta T_1$			$\Delta T_2$			$\Delta T_3$			$\Delta T_4$		
4	$\Delta T_1$			$\Delta T_2$			$\Delta T_3$			$\Delta T_4$		
5	$\Delta T_1$			$\Delta T_2$			$\Delta T_3$			$\Delta T_4$		
6	$\Delta T_1$			$\Delta T_2$			$\Delta T_3$			$\Delta T_4$		
7	$\Delta T_1$			$\Delta T_2$			$\Delta T_3$			$\Delta T_4$		
8	$\Delta T_1$			$\Delta T_2$			$\Delta T_3$			$\Delta T_4$		

Figure 7b

TX	OFDM Frame number											
	12H+1	12H+2	12H+3	12H+4	12H+5	12H+6	12H+7	12H+8	12H+9	12H+10	12H+11	12H+12
1	$\Delta T_1$	SY		$\Delta T_2$			$\Delta T_3$			$\Delta T_4$		
2	$\Delta T_1$		SY	$\Delta T_2$			$\Delta T_3$			$\Delta T_4$		
3	$\Delta T_1$			$\Delta T_2$	SY		$\Delta T_3$			$\Delta T_4$		
4	$\Delta T_1$			$\Delta T_2$		SY	$\Delta T_3$			$\Delta T_4$		
5	$\Delta T_1$			$\Delta T_2$			$\Delta T_3$	SY		$\Delta T_4$		
6	$\Delta T_1$			$\Delta T_2$			$\Delta T_3$		SY	$\Delta T_4$		
7	$\Delta T_1$			$\Delta T_2$			$\Delta T_3$			$\Delta T_4$	SY	
8	$\Delta T_1$			$\Delta T_2$			$\Delta T_3$			$\Delta T_4$		SY

Figure 7c

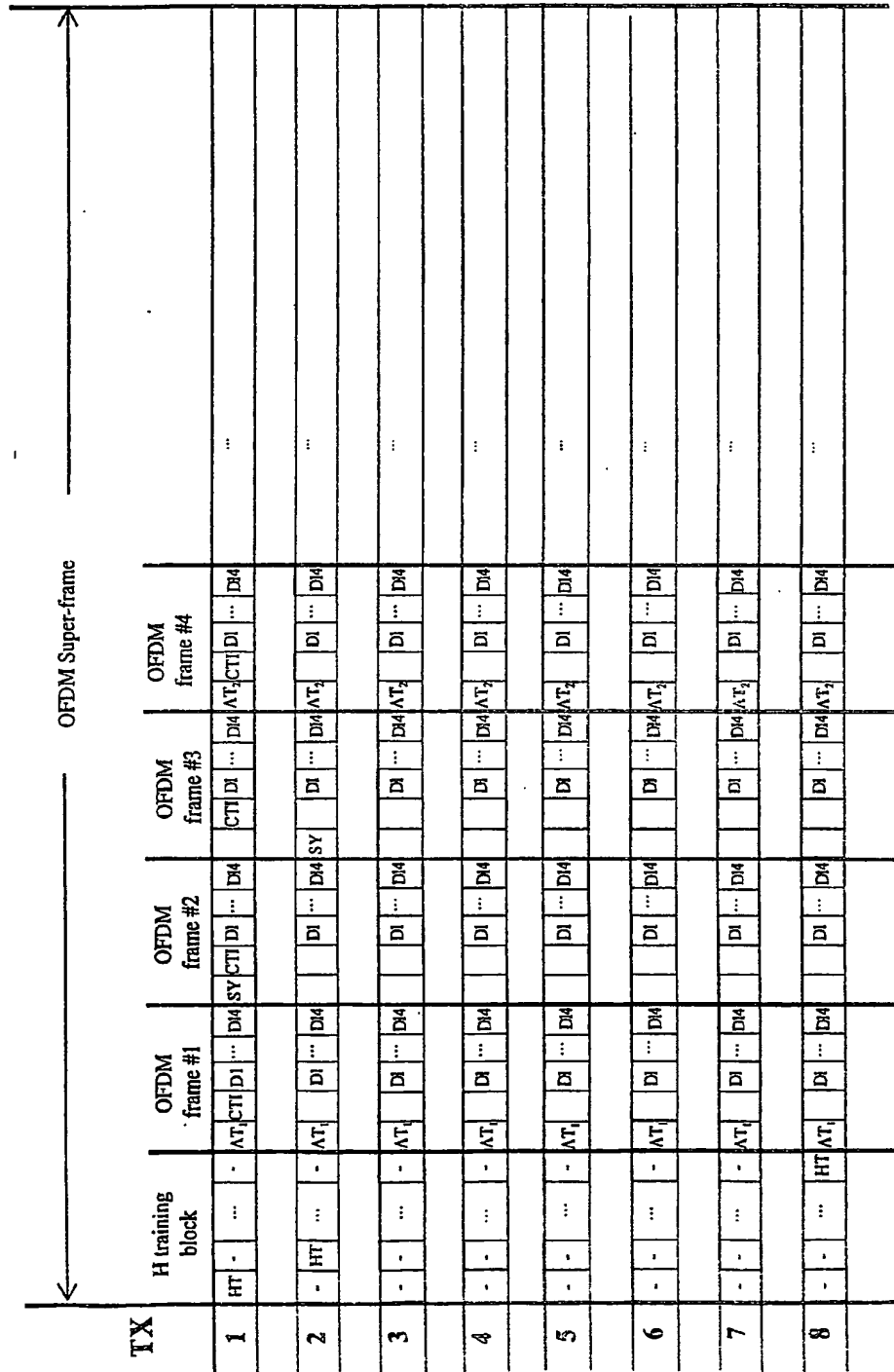


Figure 8

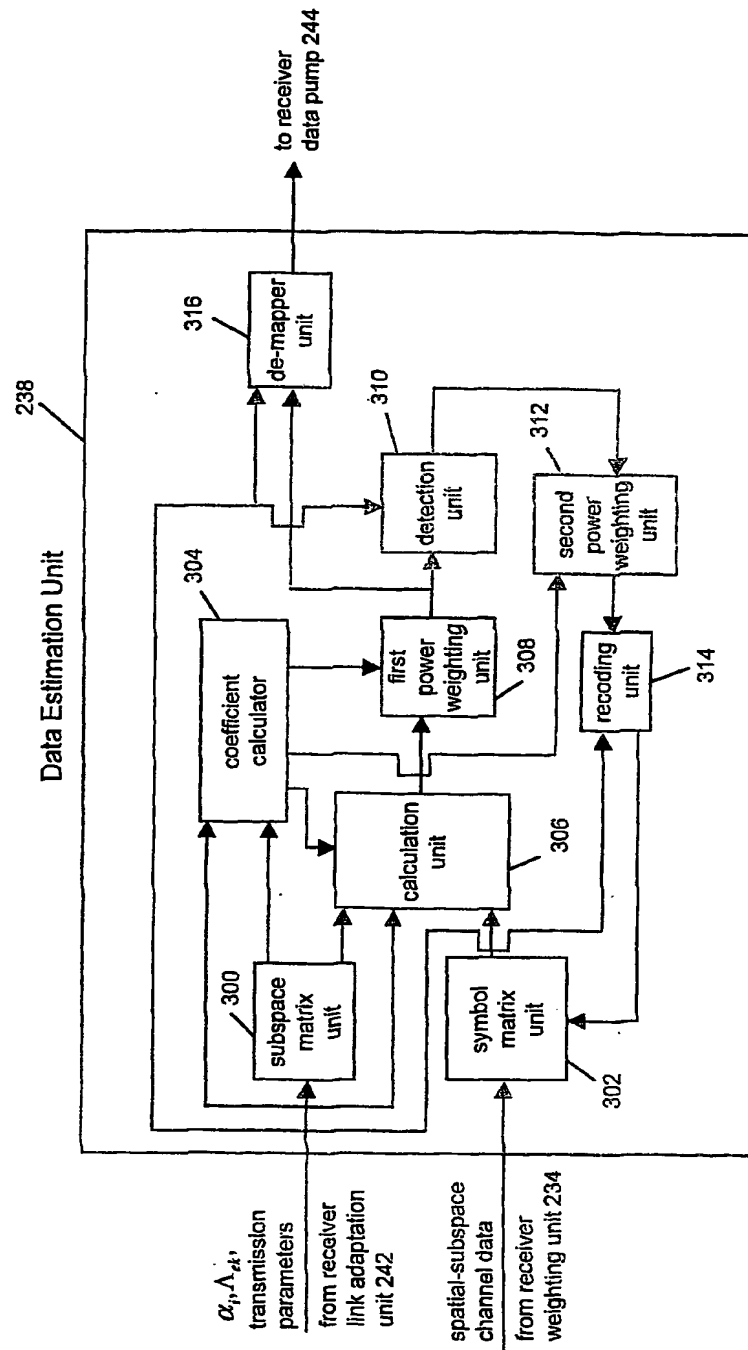


Figure 9



(43) International Publication Date  
4 December 2003 (04.12.2003)

PCT

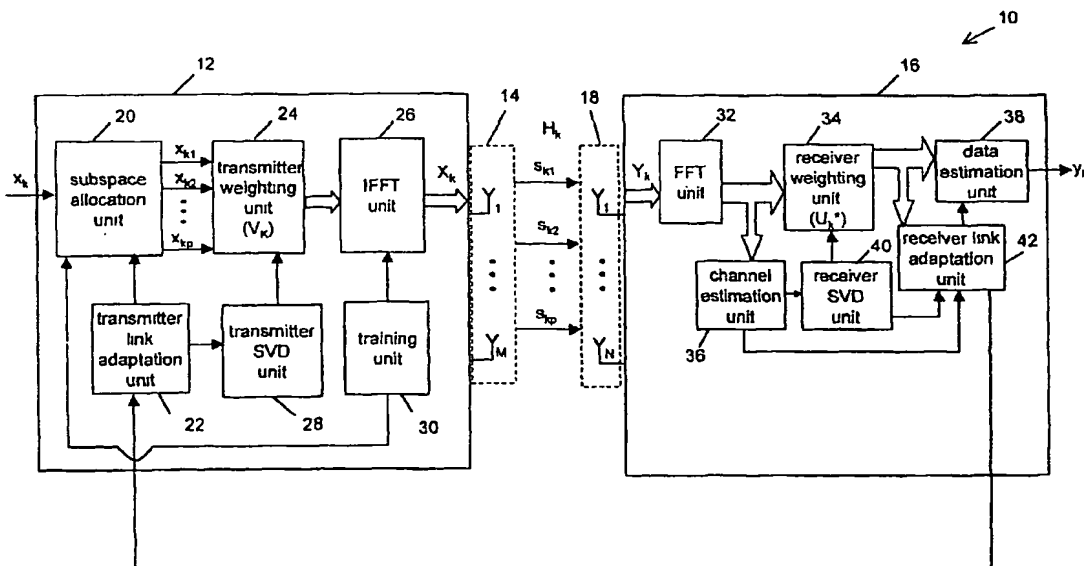
(10) International Publication Number  
WO 2003/100986 A3

A2

- (51) International Patent Classification<sup>7</sup>: H04B 7/08, H04L 27/26
- (21) International Application Number: PCT/CA2003/000737
- (22) International Filing Date: 23 May 2003 (23.05.2003)
- (25) Filing Language: English
- (26) Publication Language: English
- (30) Priority Data:  
60/382,581 24 May 2002 (24.05.2002) US  
10/402,215 31 March 2003 (31.03.2003) US
- (71) Applicant (for all designated States except US): AVENDO WIRELESS INC. [CA/CA]; 2595 Skymark Avenue, Unit 209, Mississauga, Ontario L4W 4L5 (CA).
- (72) Inventors; and
- (75) Inventors/Applicants (for US only): OPREA, Alexandru, M. [CA/CA]; 25 Farmcote Road, North York, Ontario M3B 2Z6 (CA). ZAMIRI-JAFARIAN, Hossein [IR/CA]; 25 Saint Mary Street, Apt. 308, Toronto, Ontario M4Y 1R2 (CA).
- (74) Agent: BERESKIN & PARR; 40 King Street West, 40th Floor, Toronto, Ontario M5H 3Y2 (CA).
- (81) Designated States (national): AE, AG, AL, AM, AT, AU, AZ, BA, BB, BG, BR, BY, BZ, CA, CH, CN, CO, CR, CU, CZ, DE, DK, DM, DZ, EC, EE, ES, FI, GB, GD, GE, GH, GM, HR, HU, ID, IL, IN, IS, JP, KE, KG, KP, KR, KZ, LC, LK, LR, LS, LT, LU, LV, MA, MD, MG, MK, MN, MW, MX, MZ, NO, NZ, OM, PH, PL, PT, RO, RU, SC, SD, SE, SG, SK, SL, TJ, TM, TN, TR, TT, TZ, UA, UG, US, UZ, VC, VN, YU, ZA, ZM, ZW.
- (84) Designated States (regional): ARIPO patent (GH, GM, KE, LS, MW, MZ, SD, SL, SZ, TZ, UG, ZM, ZW), Eurasian patent (AM, AZ, BY, KG, KZ, MD, RU, TJ, TM), European patent (AT, BE, BG, CH, CY, CZ, DE, DK, EE, ES, FI, FR, GB, GR, HU, IE, IT, LU, MC, NL, PT, RO, SE, SI, SK, TR), OAPI patent (BF, BJ, CF, CG, CI, CM, GA, GN, GQ, GW, ML, MR, NE, SN, TD, TG).
- Published:  
— with international search report  
— before the expiration of the time limit for amending the claims and to be republished in the event of receipt of amendments

[Continued on next page]

(54) Title: DATA DETECTION METHOD FOR MIMO-OFDM COMMUNICATION SYSTEMS



(57) Abstract: A system and method for data detection in a wireless communication system wherein the system comprises a receiver for receiving spatial-subspace data transmitted over a plurality of spatial-subspace channels of a sub-carrier which may comprise at least one of coded and uncoded spatial-subspace channels. The receiver comprises a receiver weighting unit for providing receive-weighted spatial-subspace data and a data estimation unit for performing an iterative processing method on the receive-weighted spatial-subspace data to estimate output data related to the input data symbol stream. The iterative processing method comprises successively processing data on each of the plurality of spatial-subspace channels in the receive-weighted spatial-subspace data.



(88) Date of publication of the international search report:  
5 February 2004

*For two-letter codes and other abbreviations, refer to the "Guidance Notes on Codes and Abbreviations" appearing at the beginning of each regular issue of the PCT Gazette.*

# INTERNATIONAL SEARCH REPORT

International Application No

PCT/CA 03/00737

**A. CLASSIFICATION OF SUBJECT MATTER**  
IPC. 7 H04B7/08 H04L27/26

According to International Patent Classification (IPC) or to both national classification and IPC

## B. FIELDS SEARCHED

Minimum documentation searched (classification system followed by classification symbols)

IPC 7 H04B H04L

Documentation searched other than minimum documentation to the extent that such documents are included in the fields searched

Electronic data base consulted during the international search (name of data base and, where practical, search terms used)

EPO-Internal, WPI Data, PAJ

## C. DOCUMENTS CONSIDERED TO BE RELEVANT

Category *	Citation of document, with indication, where appropriate, of the relevant passages	Relevant to claim No.
Y	US 6 377 631 B1 (RALEIGH GREGORY G) 23 April 2002 (2002-04-23) abstract column 4, line 28 - line 31 column 6, line 46 - line 66 column 8, line 34 - line 67 claim 1	1-42
Y	EP 1 185 048 A (NORTEL NETWORKS LTD) 6 March 2002 (2002-03-06) abstract column 3, line 6 - line 9 claims 1,2	1-42



Further documents are listed in the continuation of box C.



Patent family members are listed in annex.

\* Special categories of cited documents:

\*A\* document defining the general state of the art which is not considered to be of particular relevance

\*E\* earlier document but published on or after the international filing date

\*L\* document which may throw doubts on priority claim(s) or which is cited to establish the publication date of another citation or other special reason (as specified)

\*O\* document referring to an oral disclosure, use, exhibition or other means

\*P\* document published prior to the international filing date but later than the priority date claimed

\*T\* later document published after the international filing date or priority date and not in conflict with the application but cited to understand the principle or theory underlying the invention

\*X\* document of particular relevance; the claimed invention cannot be considered novel or cannot be considered to involve an inventive step when the document is taken alone

\*Y\* document of particular relevance; the claimed invention cannot be considered to involve an inventive step when the document is combined with one or more other such documents, such combination being obvious to a person skilled in the art.

\* & \* document member of the same patent family

Date of the actual completion of the international search

12 November 2003

Date of mailing of the international search report

26/11/2003

Name and mailing address of the ISA

European Patent Office, P.B. 5818 Patentlaan 2  
NL - 2280 HV Rijswijk  
Tel. (+31-70) 340-2040, Tx. 31 651 epo nl,  
Fax: (+31-70) 340-3016

Authorized officer

Mier, A

BEST AVAILABLE COPY

# INTERNATIONAL SEARCH REPORT

International Application No

PCT/CA 03/00737

## C.(Continuation) DOCUMENTS CONSIDERED TO BE RELEVANT

Category *	Citation of document, with indication, where appropriate, of the relevant passages	Relevant to claim No.
A	<p>CIMINI L J ET AL: "CLUSTERED OFDM WITH TRANSMITTER DIVERSITY AND CODING" COMMUNICATIONS: THE KEY TO GLOBAL PROSPERITY. GLOBECOM 1996. LONDON, NOV. 18 - 22, 1996, GLOBAL TELECOMMUNICATIONS CONFERENCE (GLOBECOM), NEW YORK, IEEE, US, vol. 1, 18 November 1996 (1996-11-18), pages 703-707, XP000742231  ISBN: 0-7803-3337-3  abstract  figure 1</p>	1-42
A	<p>EP 1 185 001 A (NORTEL NETWORKS LTD)  6 March 2002 (2002-03-06)  abstract  claims 1,2,8,9</p>	1-42



# INTERNATIONAL SEARCH REPORT

Information on patent family members

International Application No

PCT/CA 03/00737

Patent document cited in search report	Publication date	Patent family member(s)	Publication date
US 6377631	B1	23-04-2002	US 6144711 A 07-11-2000
			US 2003072382 A1 17-04-2003
			US 6452981 B1 17-09-2002
			AU 4238697 A 19-03-1998
			CA 2302289 A1 05-03-1998
			EP 0920738 A1 09-06-1999
			EP 0931388 A2 28-07-1999
			JP 2001505723 T 24-04-2001
			WO 9809385 A2 05-03-1998
			WO 9809381 A1 05-03-1998
			WO 9809395 A1 05-03-1998
EP 1185048	A	06-03-2002	US 2002041635 A1 11-04-2002
			CA 2351140 A1 01-03-2002
			CA 2355433 A1 01-03-2002
			EP 1185001 A2 06-03-2002
			EP 1185048 A2 06-03-2002
			US 2002122383 A1 05-09-2002
			US 2002122381 A1 05-09-2002
			US 2002122382 A1 05-09-2002
EP 1185001	A	06-03-2002	US 2002122383 A1 05-09-2002
			CA 2351140 A1 01-03-2002
			CA 2355433 A1 01-03-2002
			EP 1185001 A2 06-03-2002
			EP 1185048 A2 06-03-2002
			US 2002122381 A1 05-09-2002
			US 2002122382 A1 05-09-2002
			US 2002041635 A1 11-04-2002

BEST AVAILABLE COPY